

# LM2596 SIMPLE SWITCHER<sup>®</sup>電力コンバータ、150kHz

## 3A降圧型電圧レギュレータ

### 1 特長

- 3.3V、5V、12V、および可変出力バージョン
- 可変タイプの出力電圧範囲は1.2Vから最大37V、入力と負荷の全条件で $\pm 4\%$ の許容誤差
- TO-220およびTO-263パッケージで供給
- 3Aの出力負荷電流
- 最大40Vの入力電圧範囲
- 4個の外付け部品で動作可能
- 優れたラインおよび負荷レギュレーション仕様
- 150kHz固定周波数の内部オシレータ
- TTLシャットダウン機能
- 低消費電力のスタンバイ・モード、 $I_Q$ の標準値 80 $\mu$ A
- 高効率
- 容易に入手可能な標準インダクタ使用
- サーマル・シャットダウンおよび電流制限保護

### 2 アプリケーション

- シンプルな高効率降圧型(バック)レギュレータ
- オンボード・スイッチング・レギュレータ
- 反転型コンバータ

### 3 概要

LM2596シリーズのレギュレータは、降圧型(バック)スイッチング・レギュレータのすべてのアクティブ機能を内蔵したモノリシックICで、優れたラインおよび負荷レギュレーションで3Aの負荷を駆動できます。これらのデバイスは、3.3V、5V、12Vの固定出力電圧と、可変出力バージョンで利用可能です。

これらのレギュレータは、必要な外部コンポーネントの数が最小限で、簡単に使用でき、内部的な周波数補償と固定周波数発振器が内蔵されています。

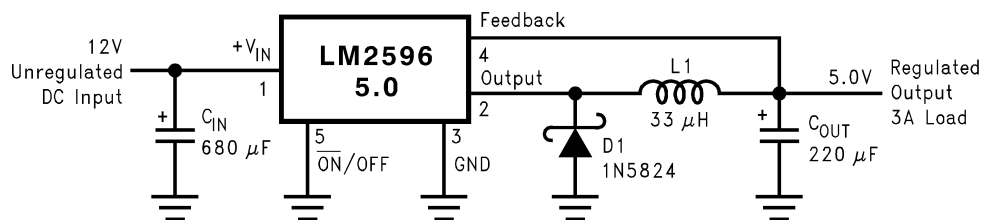
LM2596シリーズは150kHzのスイッチング周波数で動作するため、低周波数で動作するスイッチング・レギュレータに比べて、サイズの小さなフィルタ部品を使用できます。標準的な7ピンのTO-220パッケージで、いくつかの異なるリードフォーミング品で供給されるほか、7ピンのTO-263表面実装パッケージでも供給されます。

#### 製品情報<sup>(1)</sup>

型番	パッケージ	本体サイズ(公称)
LM2596	TO-220 (7)	14.986mm×10.16mm
	TO-263 (7)	10.10mm×8.89mm

(1) 提供されているすべてのパッケージについては、巻末の注文情報を参照してください。

#### 代表的なアプリケーション



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(固定出力電圧バージョン)

## 目次

<b>1</b>	<b>特長</b> .....	<b>1</b>	<b>8</b>	<b>Detailed Description</b> .....	<b>10</b>
<b>2</b>	<b>アプリケーション</b> .....	<b>1</b>	8.1	Overview .....	10
<b>3</b>	<b>概要</b> .....	<b>1</b>	8.2	Functional Block Diagram .....	10
<b>4</b>	<b>改訂履歴</b> .....	<b>2</b>	8.3	Feature Description .....	10
<b>5</b>	<b>概要 (続き)</b> .....	<b>3</b>	8.4	Device Functional Modes .....	14
<b>6</b>	<b>Pin Configuration and Functions</b> .....	<b>3</b>	<b>9</b>	<b>Application and Implementation</b> .....	<b>15</b>
<b>7</b>	<b>Specifications</b> .....	<b>4</b>	9.1	Application Information .....	15
7.1	Absolute Maximum Ratings .....	4	9.2	Typical Applications .....	22
7.2	ESD Ratings .....	4	<b>10</b>	<b>Power Supply Recommendations</b> .....	<b>31</b>
7.3	Operating Conditions .....	4	<b>11</b>	<b>Layout</b> .....	<b>31</b>
7.4	Thermal Information .....	4	11.1	Layout Guidelines .....	31
7.5	Electrical Characteristics – 3.3-V Version .....	5	11.2	Layout Examples .....	31
7.6	Electrical Characteristics – 5-V Version .....	5	11.3	Thermal Considerations .....	33
7.7	Electrical Characteristics – 12-V Version .....	5	<b>12</b>	<b>デバイスおよびドキュメントのサポート</b> .....	<b>35</b>
7.8	Electrical Characteristics – Adjustable Voltage Version .....	5	12.1	コミュニティ・リソース .....	35
7.9	Electrical Characteristics – All Output Voltage Versions .....	6	12.2	商標 .....	35
7.10	Typical Characteristics .....	7	12.3	静電気放電に関する注意事項 .....	35
			12.4	Glossary .....	35
			<b>13</b>	<b>メカニカル、パッケージ、および注文情報</b> .....	<b>35</b>

## 4 改訂履歴

資料番号末尾の英字は改訂を表しています。その改訂履歴は英語版に準じています。

Revision C (April 2013) から Revision D に変更	Page
• 「ESD定格」の表、「機能説明」セクション、「デバイスの機能モード」セクション、「アプリケーションと実装」セクション、「電源に関する推奨事項」セクション、「レイアウト」セクション、「デバイスおよびドキュメントのサポート」セクション、「メカニカル、パッケージ、および注文情報」セクションを追加 .....	1
• デザイン・ソフトウェア <i>Switchers Made Simple</i> への言及をすべて削除 .....	1

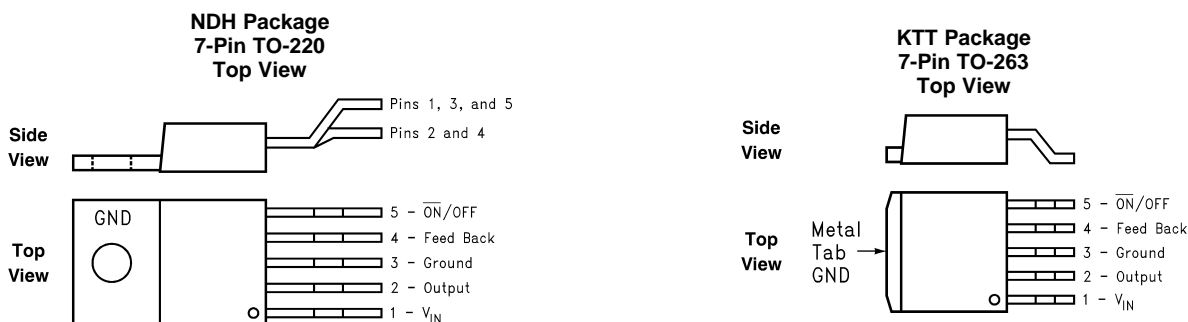
Revision B (April 2013) から Revision C に変更	Page
• Changed layout of National Semiconductor Data Sheet to TI format .....	10

## 5 概要 (続き)

LM2596シリーズでの使用に最適な標準インダクタをいくつかのメーカーから入手できます。このため、スイッチング電源の設計が大幅に簡素化されます。

また、入力電圧と出力負荷のあらゆる条件において、出力電圧について $\pm 4\%$ 、オシレータ周波数について $\pm 15\%$ の許容誤差が保証されています。外部シャットダウン機能を内蔵しており、スタンバイ電流は標準値で $80\mu\text{A}$ です。自己保護機能として、出力スイッチのための2段階周波数低下電流制限回路と、異常時でも完全に保護動作が保証される過熱シャットダウン機能を備えています。

## 6 Pin Configuration and Functions



### Pin Functions

NO.	PIN		I/O	DESCRIPTION
	NAME			
1	$V_{IN}$		I	This is the positive input supply for the IC switching regulator. A suitable input bypass capacitor must be present at this pin to minimize voltage transients and to supply the switching currents required by the regulator.
2	Output		O	Internal switch. The voltage at this pin switches between approximately $(+V_{IN} - V_{SAT})$ and approximately $-0.5\text{ V}$ , with a duty cycle of $V_{OUT} / V_{IN}$ . To minimize coupling to sensitive circuitry, the PCB copper area connected to this pin must be kept to a minimum.
3	Ground		—	Circuit ground.
4	Feedback		I	Senses the regulated output voltage to complete the feedback loop.
5	$\overline{\text{ON/OFF}}$		I	Allows the switching regulator circuit to be shut down using logic signals thus dropping the total input supply current to approximately $80\mu\text{A}$ . Pulling this pin below a threshold voltage of approximately $1.3\text{ V}$ turns the regulator on, and pulling this pin above $1.3\text{ V}$ (up to a maximum of $25\text{ V}$ ) shuts the regulator down. If this shutdown feature is not required, the $\overline{\text{ON/OFF}}$ pin can be wired to the ground pin or it can be left open. In either case, the regulator will be in the ON condition.

## 7 Specifications

### 7.1 Absolute Maximum Ratings

 over operating free-air temperature range (unless otherwise noted)<sup>(1)(2)</sup>

		MIN	MAX	UNIT
Maximum supply voltage ( $V_{IN}$ )			45	V
$\overline{SD}/SS$ pin input voltage <sup>(3)</sup>			6	V
Delay pin voltage <sup>(3)</sup>			1.5	V
Flag pin voltage		-0.3	45	V
Feedback pin voltage		-0.3	25	V
Output voltage to ground, steady-state			-1	V
Power dissipation		Internally limited		
Lead temperature	KTW package	Vapor phase (60 s)		215
		Infrared (10 s)		
	NDZ package, soldering (10 s)		260	°C
Maximum junction temperature			150	°C
Storage temperature, $T_{stg}$		-65	150	°C

- (1) Stresses beyond those listed under *Absolute Maximum Ratings* may cause permanent damage to the device. These are stress ratings only, which do not imply functional operation of the device at these or any other conditions beyond those indicated under *Recommended Operating Conditions*. Exposure to absolute-maximum-rated conditions for extended periods may affect device reliability.
- (2) If Military/Aerospace specified devices are required, please contact the Texas Instruments Sales Office/ Distributors for availability and specifications.
- (3) Voltage internally clamped. If clamp voltage is exceeded, limit current to a maximum of 1 mA.

### 7.2 ESD Ratings

			VALUE	UNIT
$V_{ESD}$	Electrostatic discharge	Human-body model (HBM), per ANSI/ESDA/JEDEC JS-001 <sup>(1)</sup>	±2000	V

- (1) JEDEC document JEP155 states that 500-V HBM allows safe manufacturing with a standard ESD control process.

### 7.3 Operating Conditions

	MIN	MAX	UNIT
Supply voltage	4.5	40	V
Temperature	-40	125	°C

### 7.4 Thermal Information

THERMAL METRIC <sup>(1)</sup>		LM2596		UNIT
		KTW (TO-263)	NDZ (TO-220)	
		7 PINS	7 PINS	
$R_{\theta JA}$	Junction-to-ambient thermal resistance <sup>(2)(3)</sup>	See <sup>(4)</sup>	50	°C/W
		See <sup>(5)</sup>	—	
		See <sup>(6)</sup>	—	
		See <sup>(7)</sup>	—	
$R_{\theta JC(top)}$	Junction-to-case (top) thermal resistance	2	2	°C/W

- (1) For more information about traditional and new thermal metrics, see the *Semiconductor and IC Package Thermal Metrics* application report, [SPRA953](#).
- (2) The package thermal impedance is calculated in accordance to JESD 51-7.
- (3) Thermal Resistances were simulated on a 4-layer, JEDEC board.
- (4) Junction to ambient thermal resistance (no external heat sink) for the package mounted TO-220 package mounted vertically, with the leads soldered to a printed circuit board with (1 oz.) copper area of approximately 1 in<sup>2</sup>.
- (5) Junction to ambient thermal resistance with the TO-263 package tab soldered to a single sided printed circuit board with 0.5 in<sup>2</sup> of 1-oz copper area.
- (6) Junction to ambient thermal resistance with the TO-263 package tab soldered to a single sided printed circuit board with 2.5 in<sup>2</sup> of 1-oz copper area.
- (7) Junction to ambient thermal resistance with the TO-263 package tab soldered to a double sided printed circuit board with 3 in<sup>2</sup> of 1-oz copper area on the LM2596S side of the board, and approximately 16 in<sup>2</sup> of copper on the other side of the PCB.

## 7.5 Electrical Characteristics – 3.3-V Version

Specifications are for  $T_J = 25^\circ\text{C}$  (unless otherwise noted)

PARAMETER	TEST CONDITIONS		MIN <sup>(1)</sup>	TYP <sup>(2)</sup>	MAX <sup>(1)</sup>	UNIT
<b>SYSTEM PARAMETERS<sup>(3)</sup></b> (see <a href="#">Figure 35</a> for test circuit)						
$V_{OUT}$ Output voltage	$4.75\text{ V} \leq V_{IN} \leq 40\text{ V}$ , $0.2\text{ A} \leq I_{LOAD} \leq 3\text{ A}$	$T_J = 25^\circ\text{C}$	3.168	3.3	3.432	V
		$-40^\circ\text{C} \leq T_J \leq 125^\circ\text{C}$	3.135		3.465	
$\eta$ Efficiency	$V_{IN} = 12\text{ V}$ , $I_{LOAD} = 3\text{ A}$		73%			

- (1) All room temperature limits are 100% production tested. All limits at temperature extremes are specified via correlation using standard Statistical Quality Control (SQC) methods. All limits are used to calculate Average Outgoing Quality Level (AOQL).
- (2) Typical numbers are at  $25^\circ\text{C}$  and represent the most likely norm.
- (3) External components such as the catch diode, inductor, input and output capacitors can affect switching regulator system performance. When the LM2596 is used as shown in [Figure 35](#), system performance is shown in the test conditions column.

## 7.6 Electrical Characteristics – 5-V Version

Specifications are for  $T_J = 25^\circ\text{C}$  (unless otherwise noted)

PARAMETER	TEST CONDITIONS		MIN <sup>(1)</sup>	TYP <sup>(2)</sup>	MAX <sup>(1)</sup>	UNIT
<b>SYSTEM PARAMETERS<sup>(3)</sup></b> (see <a href="#">Figure 35</a> for test circuit)						
$V_{OUT}$ Output voltage	$7\text{ V} \leq V_{IN} \leq 40\text{ V}$ , $0.2\text{ A} \leq I_{LOAD} \leq 3\text{ A}$	$T_J = 25^\circ\text{C}$	4.8	5	5.2	V
		$-40^\circ\text{C} \leq T_J \leq 125^\circ\text{C}$	4.75		5.25	
$\eta$ Efficiency	$V_{IN} = 12\text{ V}$ , $I_{LOAD} = 3\text{ A}$		80%			

- (1) All room temperature limits are 100% production tested. All limits at temperature extremes are specified via correlation using standard Statistical Quality Control (SQC) methods. All limits are used to calculate Average Outgoing Quality Level (AOQL).
- (2) Typical numbers are at  $25^\circ\text{C}$  and represent the most likely norm.
- (3) External components such as the catch diode, inductor, input and output capacitors can affect switching regulator system performance. When the LM2596 is used as shown in [Figure 35](#), system performance is shown in the test conditions column.

## 7.7 Electrical Characteristics – 12-V Version

Specifications are for  $T_J = 25^\circ\text{C}$  (unless otherwise noted)

PARAMETER	TEST CONDITIONS		MIN <sup>(1)</sup>	TYP <sup>(2)</sup>	MAX <sup>(1)</sup>	UNIT
<b>SYSTEM PARAMETERS<sup>(3)</sup></b> (see <a href="#">Figure 35</a> for test circuit)						
$V_{OUT}$ Output voltage	$15\text{ V} \leq V_{IN} \leq 40\text{ V}$ , $0.2\text{ A} \leq I_{LOAD} \leq 3\text{ A}$	$T_J = 25^\circ\text{C}$	11.52	12	12.48	V
		$-40^\circ\text{C} \leq T_J \leq 125^\circ\text{C}$	11.4		12.6	
$\eta$ Efficiency	$V_{IN} = 25\text{ V}$ , $I_{LOAD} = 3\text{ A}$		90%			

- (1) All room temperature limits are 100% production tested. All limits at temperature extremes are specified via correlation using standard Statistical Quality Control (SQC) methods. All limits are used to calculate Average Outgoing Quality Level (AOQL).
- (2) Typical numbers are at  $25^\circ\text{C}$  and represent the most likely norm.
- (3) External components such as the catch diode, inductor, input and output capacitors can affect switching regulator system performance. When the LM2596 is used as shown in [Figure 35](#), system performance is shown in the test conditions column.

## 7.8 Electrical Characteristics – Adjustable Voltage Version

Specifications are for  $T_J = 25^\circ\text{C}$  (unless otherwise noted)

PARAMETER	TEST CONDITIONS		MIN <sup>(1)</sup>	TYP <sup>(2)</sup>	MAX <sup>(1)</sup>	UNIT
<b>SYSTEM PARAMETERS<sup>(3)</sup></b> (see <a href="#">Figure 35</a> for test circuit)						
$V_{FB}$ Feedback voltage	$4.5\text{ V} \leq V_{IN} \leq 40\text{ V}$ , $0.2\text{ A} \leq I_{LOAD} \leq 3\text{ A}$		1.23			V
	$V_{OUT}$ programmed for 3 V (see <a href="#">Figure 35</a> for test circuit)	$T_J = 25^\circ\text{C}$	1.193		1.267	
		$-40^\circ\text{C} \leq T_J \leq 125^\circ\text{C}$	1.18		1.28	
$\eta$ Efficiency	$V_{IN} = 12\text{ V}$ , $V_{OUT} = 3\text{ V}$ , $I_{LOAD} = 3\text{ A}$		73%			

- (1) All room temperature limits are 100% production tested. All limits at temperature extremes are specified via correlation using standard Statistical Quality Control (SQC) methods. All limits are used to calculate Average Outgoing Quality Level (AOQL).
- (2) Typical numbers are at  $25^\circ\text{C}$  and represent the most likely norm.
- (3) External components such as the catch diode, inductor, input and output capacitors can affect switching regulator system performance. When the LM2596 is used as shown in [Figure 35](#), system performance is shown in the test conditions column.

## 7.9 Electrical Characteristics – All Output Voltage Versions

Specifications are for  $T_J = 25^\circ\text{C}$ ,  $I_{\text{LOAD}} = 500\text{ mA}$ ,  $V_{\text{IN}} = 12\text{ V}$  for the 3.3-V, 5-V, and adjustable version, and  $V_{\text{IN}} = 24\text{ V}$  for the 12-V version (unless otherwise noted).

PARAMETER		TEST CONDITIONS	MIN <sup>(1)</sup>	TYP <sup>(2)</sup>	MAX <sup>(1)</sup>	UNIT	
<b>DEVICE PARAMETERS</b>							
$I_b$	Feedback bias current	Adjustable version only, $V_{\text{FB}} = 1.3\text{ V}$	$T_J = 25^\circ\text{C}$	10	50	nA	
			$-40^\circ\text{C} \leq T_J \leq 125^\circ\text{C}$		100		
$f_O$	Oscillator frequency <sup>(3)</sup>	$T_J = 25^\circ\text{C}$ $-40^\circ\text{C} \leq T_J \leq 125^\circ\text{C}$		127	150	173	kHz
				110		173	
$V_{\text{SAT}}$	Saturation voltage <sup>(4)</sup> <sup>(5)</sup>	$I_{\text{OUT}} = 3\text{ A}$	$T_J = 25^\circ\text{C}$	1.16	1.4	V	
			$-40^\circ\text{C} \leq T_J \leq 125^\circ\text{C}$		1.5		
DC	Max duty cycle (ON) <sup>(5)</sup>			100%			
	Min duty cycle (OFF) <sup>(6)</sup>			0%			
$I_{\text{CL}}$	Current limit <sup>(4)</sup> <sup>(5)</sup>	Peak current	$T_J = 25^\circ\text{C}$	3.6	4.5	6.9	A
			$-40^\circ\text{C} \leq T_J \leq 125^\circ\text{C}$		3.4	7.5	
$I_L$	Output leakage current <sup>(4)</sup> <sup>(6)</sup>	Output = 0 V, $V_{\text{IN}} = 40\text{ V}$			50	$\mu\text{A}$	
		Output = -1 V		2	30	mA	
$I_Q$	Operating quiescent current <sup>(6)</sup>	See <sup>(6)</sup>		5	10	mA	
$I_{\text{STBY}}$	Current standby quiescent	$\overline{\text{ON}}/\text{OFF}$ pin = 5 V (OFF) <sup>(7)</sup>	$T_J = 25^\circ\text{C}$	80	200	$\mu\text{A}$	
			$-40^\circ\text{C} \leq T_J \leq 125^\circ\text{C}$		250	$\mu\text{A}$	
<b>SHUTDOWN/SOFT-START CONTROL</b> (see <a href="#">Figure 35</a> for test circuit)							
$V_{\text{IH}}$	$\overline{\text{ON}}/\text{OFF}$ pin logic input threshold voltage	Low (regulator ON)	$T_J = 25^\circ\text{C}$	1.3		V	
			$-40^\circ\text{C} \leq T_J \leq 125^\circ\text{C}$		0.6		
$V_{\text{IL}}$	$\overline{\text{ON}}/\text{OFF}$ pin logic input threshold voltage	High (regulator OFF)	$T_J = 25^\circ\text{C}$	1.3		V	
			$-40^\circ\text{C} \leq T_J \leq 125^\circ\text{C}$		2		
$I_H$	$\overline{\text{ON}}/\text{OFF}$ pin input current	$V_{\text{LOGIC}} = 2.5\text{ V}$ (regulator OFF)		5	15	$\mu\text{A}$	
$I_L$	$\overline{\text{ON}}/\text{OFF}$ pin input current	$V_{\text{LOGIC}} = 0.5\text{ V}$ (regulator ON)		0.02	5	$\mu\text{A}$	

- (1) All room temperature limits are 100% production tested. All limits at temperature extremes are specified via correlation using standard Statistical Quality Control (SQC) methods. All limits are used to calculate Average Outgoing Quality Level (AOQL).
- (2) Typical numbers are at  $25^\circ\text{C}$  and represent the most likely norm.
- (3) The switching frequency is reduced when the second stage current limit is activated. The amount of reduction is determined by the severity of current overload.
- (4) No diode, inductor, or capacitor connected to output pin.
- (5) Feedback pin removed from output and connected to 0 V to force the output transistor switch ON.
- (6) Feedback pin removed from output and connected to 12 V for the 3.3-V, 5-V, and the adjustable versions, and 15 V for the 12-V version, to force the output transistor switch OFF.
- (7)  $V_{\text{IN}} = 40\text{ V}$ .

### 7.10 Typical Characteristics

See Figure 35 for test circuit

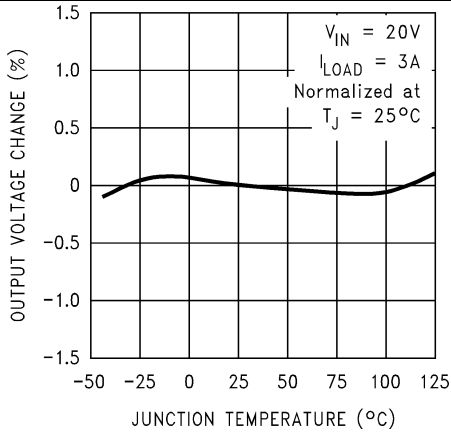


Figure 1. Normalized Output Voltage

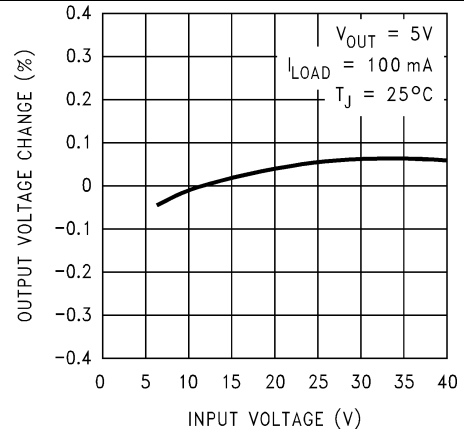


Figure 2. Line Regulation

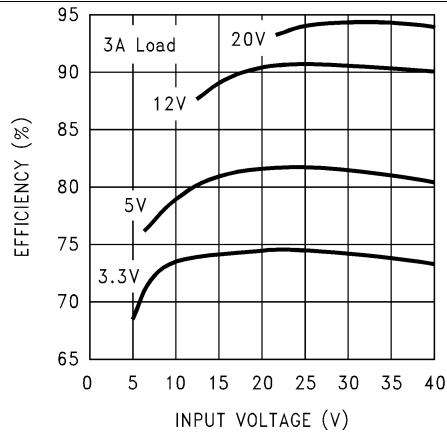


Figure 3. Efficiency

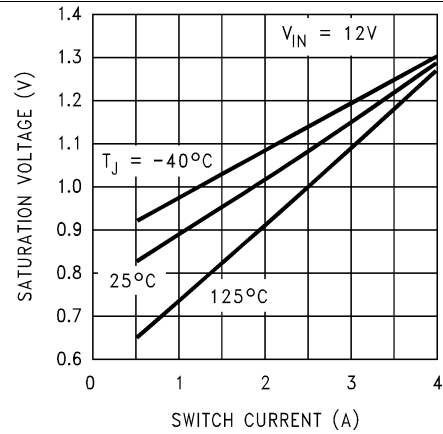


Figure 4. Switch Saturation Voltage

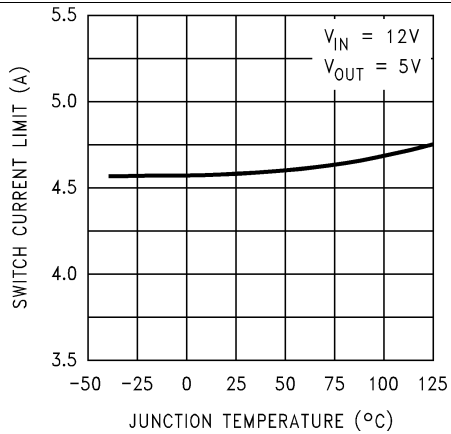


Figure 5. Switch Current Limit

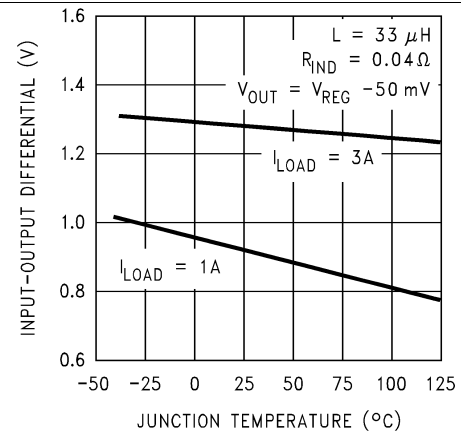


Figure 6. Dropout Voltage

Typical Characteristics (continued)

See Figure 35 for test circuit

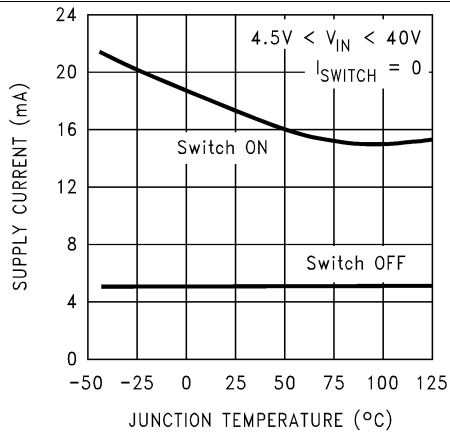


Figure 7. Operating Quiescent Current

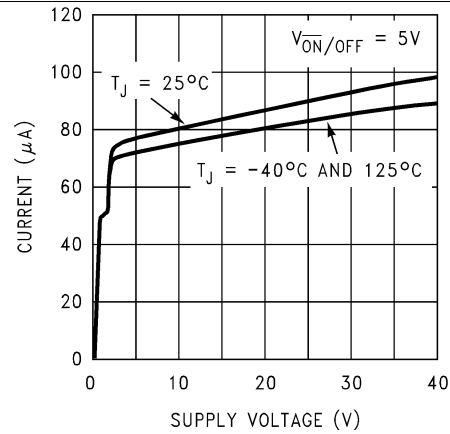


Figure 8. Shutdown Quiescent Current

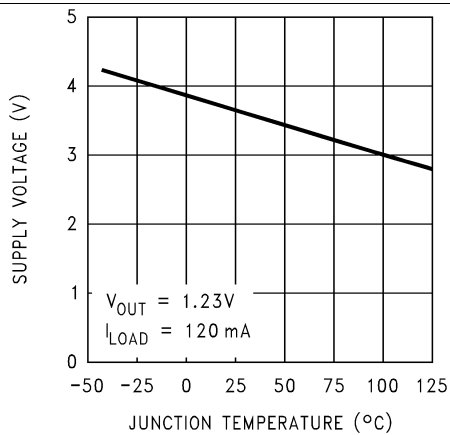


Figure 9. Minimum Operating Supply Voltage

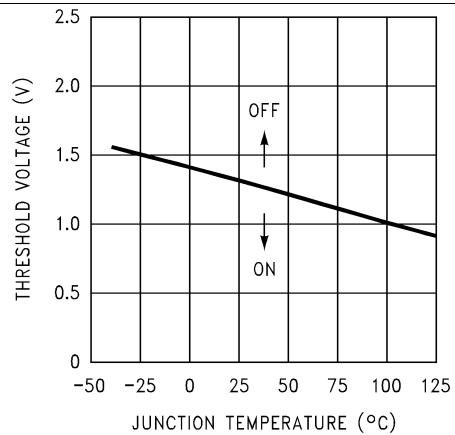


Figure 10. ON/OFF Threshold Voltage

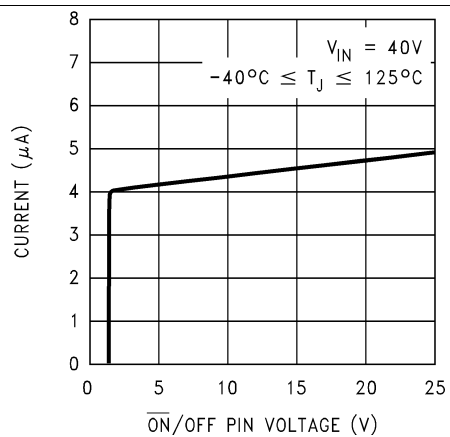


Figure 11. ON/OFF Pin Current (Sinking)

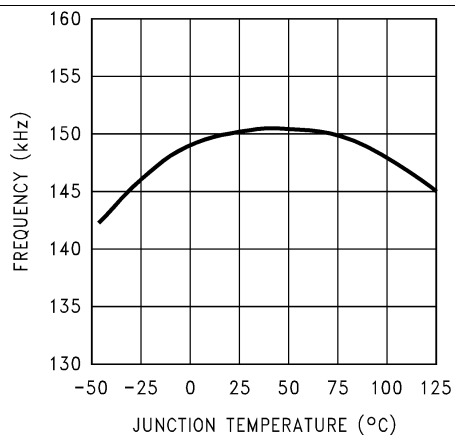
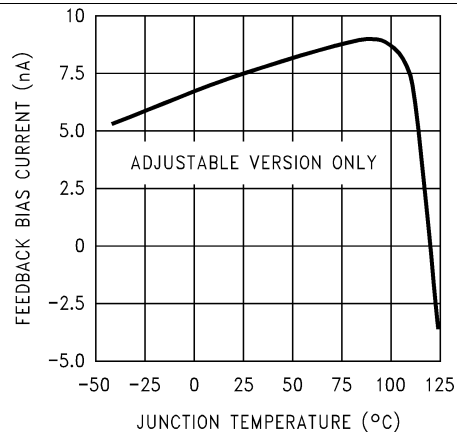


Figure 12. Switching Frequency



**Typical Characteristics (continued)**

See [Figure 35](#) for test circuit



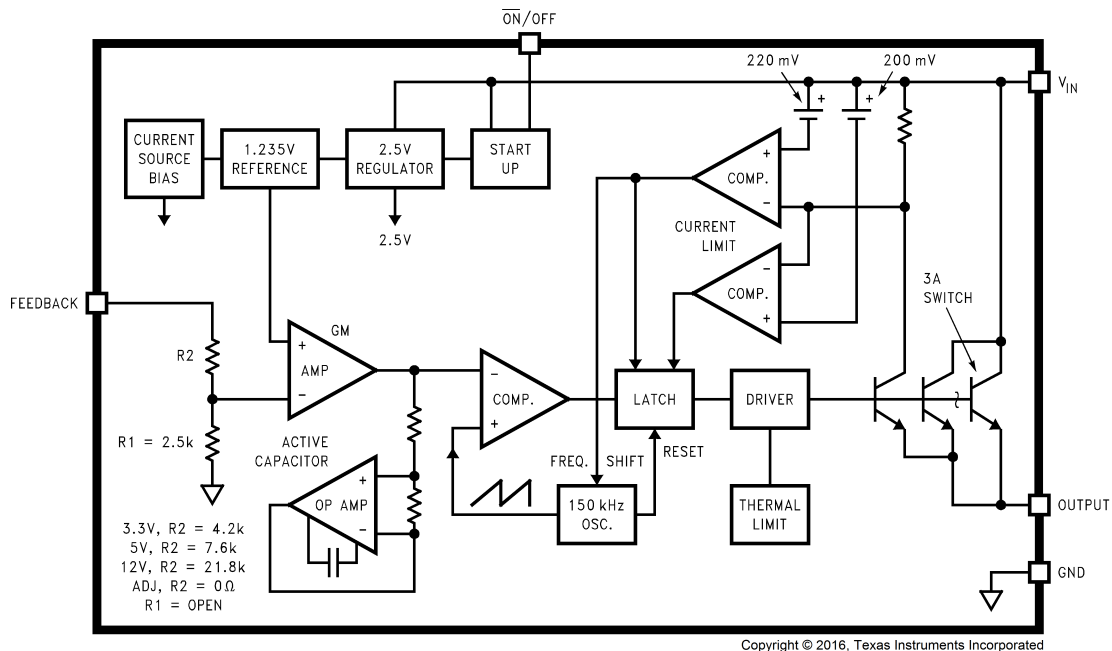
**Figure 13. Feedback Pin Bias Current**

## 8 Detailed Description

### 8.1 Overview

The LM2596 SIMPLE SWITCHER<sup>®</sup> regulator is an easy-to-use, nonsynchronous, step-down DC-DC converter with a wide input voltage range up to 40 V. The regulator is capable of delivering up to 3-A DC load current with excellent line and load regulation. These devices are available in fixed output voltages of 3.3-V, 5-V, 12-V and an adjustable output version. The family requires few external components, and the pin arrangement was designed for simple, optimum PCB layout.

### 8.2 Functional Block Diagram



### 8.3 Feature Description

#### 8.3.1 Delayed Start-Up

The circuit in [Figure 14](#) uses the  $\overline{\text{ON/OFF}}$  pin to provide a time delay between the time the input voltage is applied and the time the output voltage comes up (only the circuitry pertaining to the delayed start-up is shown). As the input voltage rises, the charging of capacitor C1 pulls the  $\overline{\text{ON/OFF}}$  pin high, keeping the regulator OFF. Once the input voltage reaches its final value and the capacitor stops charging, resistor R<sub>2</sub> pulls the  $\overline{\text{ON/OFF}}$  pin low, thus allowing the circuit to start switching. Resistor R<sub>1</sub> is included to limit the maximum voltage applied to the  $\overline{\text{ON/OFF}}$  pin (maximum of 25 V), reduces power supply noise sensitivity, and also limits the capacitor C1 discharge current. When high input ripple voltage exists, avoid long delay time, because this ripple can be coupled into the  $\overline{\text{ON/OFF}}$  pin and cause problems.

This delayed start-up feature is useful in situations where the input power source is limited in the amount of current it can deliver. It allows the input voltage to rise to a higher voltage before the regulator starts operating. Buck regulators require less input current at higher input voltages.

## Feature Description (continued)

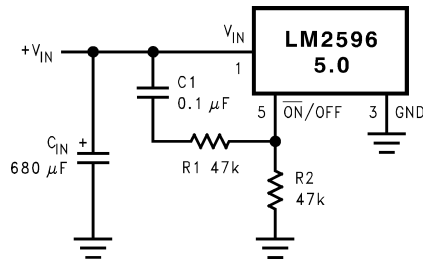


Figure 14. Delayed Start-Up

### 8.3.2 Undervoltage Lockout

Some applications require the regulator to remain off until the input voltage reaches a predetermined voltage. Figure 15 shows an undervoltage lockout feature applied to a buck regulator, while Figure 16 and Figure 17 apply the same feature to an inverting circuit. The circuit in Figure 16 features a constant threshold voltage for turnon and turnoff (Zener voltage plus approximately one volt). If hysteresis is required, the circuit in Figure 17 has a turnon voltage which is different than the turnoff voltage. The amount of hysteresis is approximately equal to the value of the output voltage. If Zener voltages greater than 25 V are used, an additional 47-kΩ resistor is required from the ON/OFF pin to the ground pin to stay within the 25 V maximum limit of the ON/OFF pin.

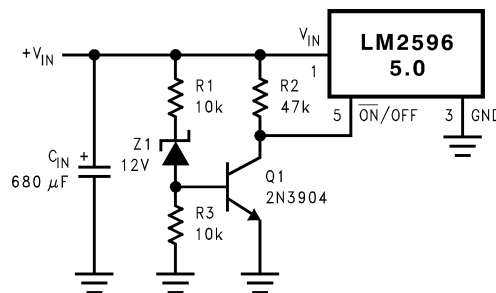
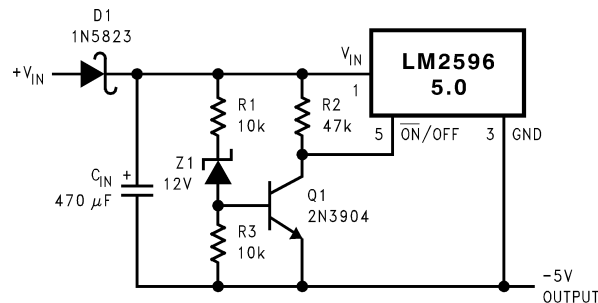


Figure 15. Undervoltage Lockout for Buck Regulator

### 8.3.3 Inverting Regulator

The circuit in Figure 18 converts a positive input voltage to a negative output voltage with a common ground. The circuit operates by bootstrapping the ground pin of the regulator to the negative output voltage, then grounding the feedback pin, the regulator senses the inverted output voltage and regulates it.



This circuit has an ON/OFF threshold of approximately 13 V.

Figure 16. Undervoltage Lockout for Inverting Regulator

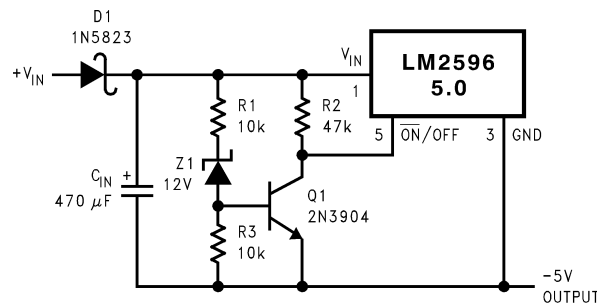
**Feature Description (continued)**

This example uses the LM2596-5.0 to generate a -5-V output, but other output voltages are possible by selecting other output voltage versions, including the adjustable version. Because this regulator topology can produce an output voltage that is either greater than or less than the input voltage, the maximum output current greatly depends on both the input and output voltage. Figure 19 provides a guide as to the amount of output load current possible for the different input and output voltage conditions.

The maximum voltage appearing across the regulator is the absolute sum of the input and output voltage, and this must be limited to a maximum of 40 V. For example, when converting +20 V to -12 V, the regulator would see 32 V between the input pin and ground pin. The LM2596 has a maximum input voltage spec of 40 V.

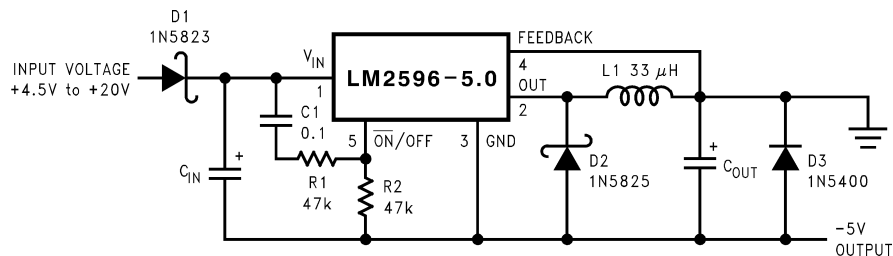
Additional diodes are required in this regulator configuration. Diode D1 is used to isolate input voltage ripple or noise from coupling through the C<sub>IN</sub> capacitor to the output, under light or no load conditions. Also, this diode isolation changes the topology to closely resemble a buck configuration, thus providing good closed-loop stability. TI recommends using a Schottky diode for low input voltages, (because of its lower voltage drop) but for higher input voltages, a fast recovery diode could be used.

Without diode D3, when the input voltage is first applied, the charging current of C<sub>IN</sub> can pull the output positive by several volts for a short period of time. Adding D3 prevents the output from going positive by more than a diode voltage.



This circuit has hysteresis  
 Regulator starts switching at V<sub>IN</sub> = 13 V  
 Regulator stops switching at V<sub>IN</sub> = 8 V

**Figure 17. Undervoltage Lockout With Hysteresis for Inverting Regulator**



C<sub>IN</sub> — 68-μF, 25-V Tant. Sprague 595D  
 470 -μF, 50-V Elec. Panasonic HFQ  
 C<sub>OUT</sub> — 47-μF, 20-V Tant. Sprague 595D  
 220-μF, 25-V Elec. Panasonic HFQ

**Figure 18. Inverting -5-V Regulator With Delayed Start-Up**

## Feature Description (continued)

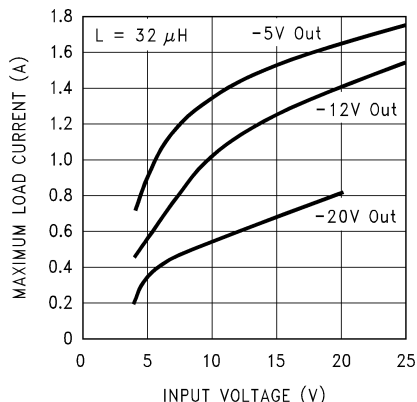


Figure 19. Inverting Regulator Typical Load Current

Because of differences in the operation of the inverting regulator, the standard design procedure is not used to select the inductor value. In the majority of designs, a 33- $\mu$ H, 3.5-A inductor is the best choice. Capacitor selection can also be narrowed down to just a few values. Using the values shown in Figure 18 will provide good results in the majority of inverting designs.

This type of inverting regulator can require relatively large amounts of input current when starting up, even with light loads. Input currents as high as the LM2596 current limit (approximately 4.5 A) are required for at least 2 ms or more, until the output reaches its nominal output voltage. The actual time depends on the output voltage and the size of the output capacitor. Input power sources that are current limited or sources that can not deliver these currents without getting loaded down, may not work correctly. Because of the relatively high start-up currents required by the inverting topology, the delayed start-up feature (C1, R1, and R2) shown in Figure 18 is recommended. By delaying the regulator start-up, the input capacitor is allowed to charge up to a higher voltage before the switcher begins operating. A portion of the high input current required for start-up is now supplied by the input capacitor (C<sub>IN</sub>). For severe start-up conditions, the input capacitor can be made much larger than normal.

### 8.3.4 Inverting Regulator Shutdown Methods

Using the  $\overline{\text{ON}}/\text{OFF}$  pin in a standard buck configuration is simple. To turn the regulator ON, pull the  $\overline{\text{ON}}/\text{OFF}$  pin below 1.3 V (at 25°C, referenced to ground). To turn the regulator OFF, pull the  $\overline{\text{ON}}/\text{OFF}$  pin above 1.3 V. With the inverting configuration, some level shifting is required, because the ground pin of the regulator is no longer at ground, but is now setting at the negative output voltage level. Two different shutdown methods for inverting regulators are shown in Figure 20 and Figure 21.

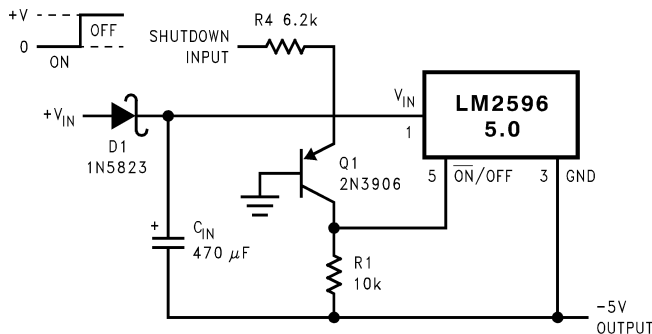
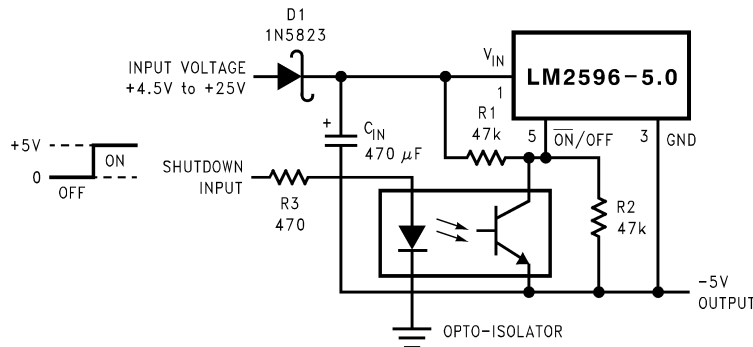


Figure 20. Inverting Regulator Ground Referenced Shutdown

**Feature Description (continued)**



**Figure 21. Inverting Regulator Ground Referenced Shutdown Using Opto Device**

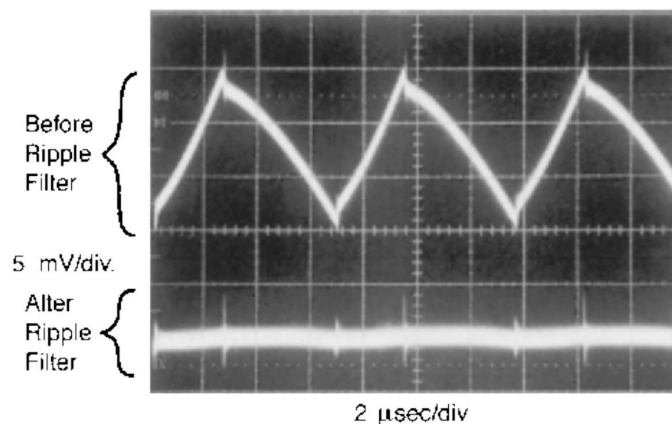
**8.4 Device Functional Modes**

**8.4.1 Discontinuous Mode Operation**

The selection guide chooses inductor values suitable for continuous mode operation, but for low current applications or high input voltages, a discontinuous mode design may be a better choice. A discontinuous mode design would use an inductor that would be physically smaller, and would require only one half to one third the inductance value required for a continuous mode design. The peak switch and inductor currents will be higher in a discontinuous design, but at these low load currents (1 A and below), the maximum switch current will still be less than the switch current limit.

Discontinuous operation can have voltage waveforms that are considerably different than a continuous design. The output pin (switch) waveform can have some damped sinusoidal ringing present (see [Figure 36](#)). This ringing is normal for discontinuous operation, and is not caused by feedback loop instabilities. In discontinuous operation, there is a period of time where neither the switch nor the diode are conducting, and the inductor current has dropped to zero. During this time, a small amount of energy can circulate between the inductor and the switch/diode parasitic capacitance causing this characteristic ringing. Normally this ringing is not a problem, unless the amplitude becomes great enough to exceed the input voltage, and even then, there is very little energy present to cause damage.

Different inductor types or core materials produce different amounts of this characteristic ringing. Ferrite core inductors have very little core loss and therefore produce the most ringing. The higher core loss of powdered iron inductors produce less ringing. If desired, a series RC could be placed in parallel with the inductor to dampen the ringing.



**Figure 22. Post Ripple Filter Waveform**

## 9 Application and Implementation

### NOTE

Information in the following applications sections is not part of the TI component specification, and TI does not warrant its accuracy or completeness. TI's customers are responsible for determining suitability of components for their purposes. Customers should validate and test their design implementation to confirm system functionality.

### 9.1 Application Information

#### 9.1.1 Input Capacitor ( $C_{IN}$ )

A low ESR aluminum or tantalum bypass capacitor is required between the input pin and ground pin. It must be placed near the regulator using short leads. This capacitor prevents large voltage transients from occurring at the input, and provides the instantaneous current required each time the switch turns ON.

The important parameters for the Input capacitor are the voltage rating and the RMS current rating. Because of the relatively high RMS currents flowing in a buck regulator's input capacitor, this capacitor must be chosen for its RMS current rating rather than its capacitance or voltage ratings, although the capacitance value and voltage rating are directly related to the RMS current rating.

The RMS current rating of a capacitor could be viewed as a capacitor's power rating. The RMS current flowing through the capacitor's internal ESR produces power which causes the internal temperature of the capacitor to rise. The RMS current rating of a capacitor is determined by the amount of current required to raise the internal temperature approximately 10°C above an ambient temperature of 105°C. The ability of the capacitor to dissipate this heat to the surrounding air will determine the amount of current the capacitor can safely sustain. For a given capacitor value, a higher voltage electrolytic capacitor will be physically larger than a lower voltage capacitor, and thus be able to dissipate more heat to the surrounding air, and therefore will have a higher RMS current rating.

The consequences of operating an electrolytic capacitor above the RMS current rating is a shortened operating life. The higher temperature speeds up the evaporation of the capacitor's electrolyte, resulting in eventual failure.

Selecting an input capacitor requires consulting the manufacturer's data sheet for maximum allowable RMS ripple current. For a maximum ambient temperature of 40°C, a general guideline would be to select a capacitor with a ripple current rating of approximately 50% of the DC load current. For ambient temperatures up to 70°C, a current rating of 75% of the DC load current would be a good choice for a conservative design. The capacitor voltage rating must be at least 1.25 times greater than the maximum input voltage, and often a much higher voltage capacitor is required to satisfy the RMS current requirements.

[Figure 23](#) shows the relationship between an electrolytic capacitor value, its voltage rating, and the RMS current it is rated for. These curves were obtained from the Nichicon *PL* series of low-ESR, high-reliability electrolytic capacitors designed for switching regulator applications. Other capacitor manufacturers offer similar types of capacitors, but always check the capacitor data sheet.

*Standard* electrolytic capacitors typically have much higher ESR numbers, lower RMS current ratings and typically have a shorter operating lifetime.

Because of their small size and excellent performance, surface-mount solid tantalum capacitors are often used for input bypassing, but several precautions must be observed. A small percentage of solid tantalum capacitors can short if the inrush current rating is exceeded. This can happen at turnon when the input voltage is suddenly applied, and of course, higher input voltages produce higher inrush currents. Several capacitor manufacturers do a 100% surge current testing on their products to minimize this potential problem. If high turnon currents are expected, it may be necessary to limit this current by adding either some resistance or inductance before the tantalum capacitor, or select a higher voltage capacitor. As with aluminum electrolytic capacitors, the RMS ripple current rating must be sized to the load current.

## Application Information (continued)

### 9.1.2 Feedforward Capacitor ( $C_{FF}$ )

#### NOTE

For adjustable output voltage version only.

A feedforward capacitor, shown across R2 in [Table 6](#), is used when the output voltage is greater than 10 V or when  $C_{OUT}$  has a very low ESR. This capacitor adds lead compensation to the feedback loop and increases the phase margin for better loop stability. For  $C_{FF}$  selection, see the [Detailed Design Procedure](#) section.

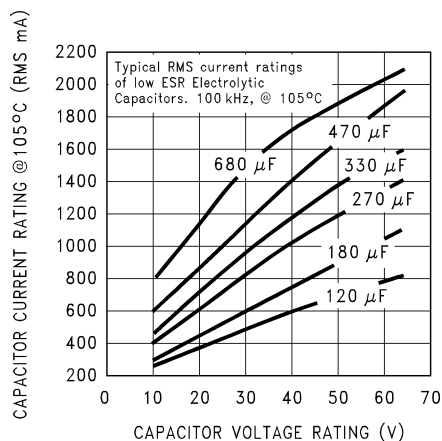


Figure 23. RMS Current Ratings for Low ESR Electrolytic Capacitors (Typical)

### 9.1.3 Output Capacitor ( $C_{OUT}$ )

An output capacitor is required to filter the output and provide regulator loop stability. Low impedance or low-ESR electrolytic or solid tantalum capacitors designed for switching regulator applications must be used. When selecting an output capacitor, the important capacitor parameters are the 100-kHz ESR, the RMS ripple current rating, voltage rating, and capacitance value. For the output capacitor, the ESR value is the most important parameter.

The output capacitor requires an ESR value that has an upper and lower limit. For low output ripple voltage, a low ESR value is required. This value is determined by the maximum allowable output ripple voltage, typically 1% to 2% of the output voltage. But if the selected capacitor's ESR is extremely low, there is a possibility of an unstable feedback loop, resulting in an oscillation at the output. Using the capacitors listed in the tables, or similar types, will provide design solutions under all conditions.

If very low output ripple voltage (less than 15 mV) is required, see [Output Voltage Ripple and Transients](#) for a post ripple filter.

An aluminum electrolytic capacitor's ESR value is related to the capacitance value and its voltage rating. In most cases, higher voltage electrolytic capacitors have lower ESR values (see [Figure 24](#)). Often, capacitors with much higher voltage ratings may be required to provide the low ESR values required for low output ripple voltage.

The output capacitor for many different switcher designs often can be satisfied with only three or four different capacitor values and several different voltage ratings. See [Table 3](#) and [Table 4](#) for typical capacitor values, voltage ratings, and manufacturers capacitor types.

Electrolytic capacitors are not recommended for temperatures below  $-25^{\circ}C$ . The ESR rises dramatically at cold temperatures and is typically 3 times as large at  $-25^{\circ}C$  and as much as 10 times as large at  $-40^{\circ}C$ . See [Figure 25](#).

Solid tantalum capacitors have a much better ESR specifications for cold temperatures and are recommended for temperatures below  $-25^{\circ}C$ .



Application Information (continued)

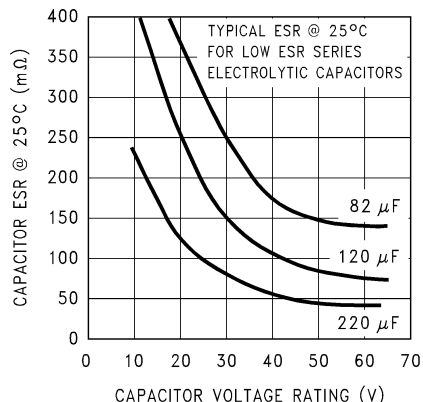


Figure 24. Capacitor ESR vs Capacitor Voltage Rating (Typical Low-ESR Electrolytic Capacitor)

9.1.4 Catch Diode

Buck regulators require a diode to provide a return path for the inductor current when the switch turns off. This must be a fast diode and must be placed close to the LM2596 using short leads and short printed-circuit traces.

Because of their very fast switching speed and low forward voltage drop, Schottky diodes provide the best performance, especially in low output voltage applications (5 V and lower). Ultra-fast recovery, or high-efficiency rectifiers are also a good choice, but some types with an abrupt turnoff characteristic may cause instability or EMI problems. Ultra-fast recovery diodes typically have reverse recovery times of 50 ns or less. Rectifiers such as the 1N5400 series are much too slow and should not be used.

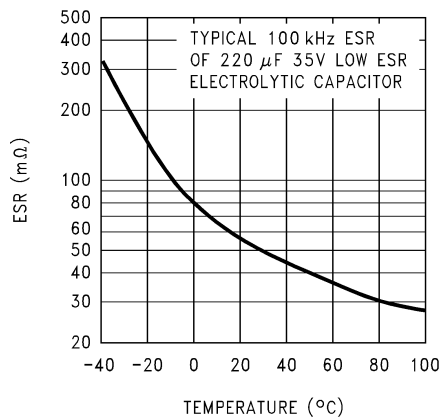


Figure 25. Capacitor ESR Change vs Temperature

9.1.5 Inductor Selection

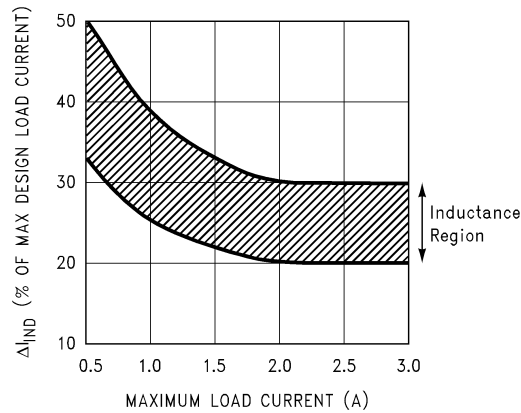
All switching regulators have two basic modes of operation; continuous and discontinuous. The difference between the two types relates to the inductor current, whether it is flowing continuously, or if it drops to zero for a period of time in the normal switching cycle. Each mode has distinctively different operating characteristics, which can affect the regulators performance and requirements. Most switcher designs will operate in the discontinuous mode when the load current is low.

The LM2596 (or any of the SIMPLE SWITCHER™ family) can be used for both continuous or discontinuous modes of operation.

In many cases the preferred mode of operation is the continuous mode, which offers greater output power, lower peak switch, lower inductor and diode currents, and can have lower output ripple voltage. However, the continuous mode does require larger inductor values to keep the inductor current flowing continuously, especially at low output load currents or high input voltages.

### Application Information (continued)

To simplify the inductor selection process, an inductor selection guide (nomograph) was designed (see [Figure 27](#) through [Figure 30](#)). This guide assumes that the regulator is operating in the continuous mode, and selects an inductor that will allow a peak-to-peak inductor ripple current to be a certain percentage of the maximum design load current. This peak-to-peak inductor ripple current percentage is not fixed, but is allowed to change as different design load currents are selected (see [Figure 26](#).)



**Figure 26. ( $\Delta I_{IND}$ ) Peak-to-Peak Inductor Ripple Current (as a Percentage of the Load Current) vs Load Current**

By allowing the percentage of inductor ripple current to increase for low load currents, the inductor value and size can be kept relatively low.

When operating in the continuous mode, the inductor current waveform ranges from a triangular to a sawtooth type of waveform (depending on the input voltage), with the average value of this current waveform equal to the DC output load current.

Inductors are available in different styles such as pot core, toroid, E-core, bobbin core, and so forth, as well as different core materials, such as ferrites and powdered iron. The least expensive, the bobbin, rod or stick core, consists of wire wound on a ferrite bobbin. This type of construction makes for an inexpensive inductor, but because the magnetic flux is not completely contained within the core, it generates more Electro-Magnetic Interference (EMI). This magnetic flux can induce voltages into nearby printed-circuit traces, thus causing problems with both the switching regulator operation and nearby sensitive circuitry, and can give incorrect scope readings because of induced voltages in the scope probe (see [Open-Core Inductors](#)).

When multiple switching regulators are located on the same PCB, open-core magnetics can cause interference between two or more of the regulator circuits, especially at high currents. A torroid or E-core inductor (closed magnetic structure) should be used in these situations.

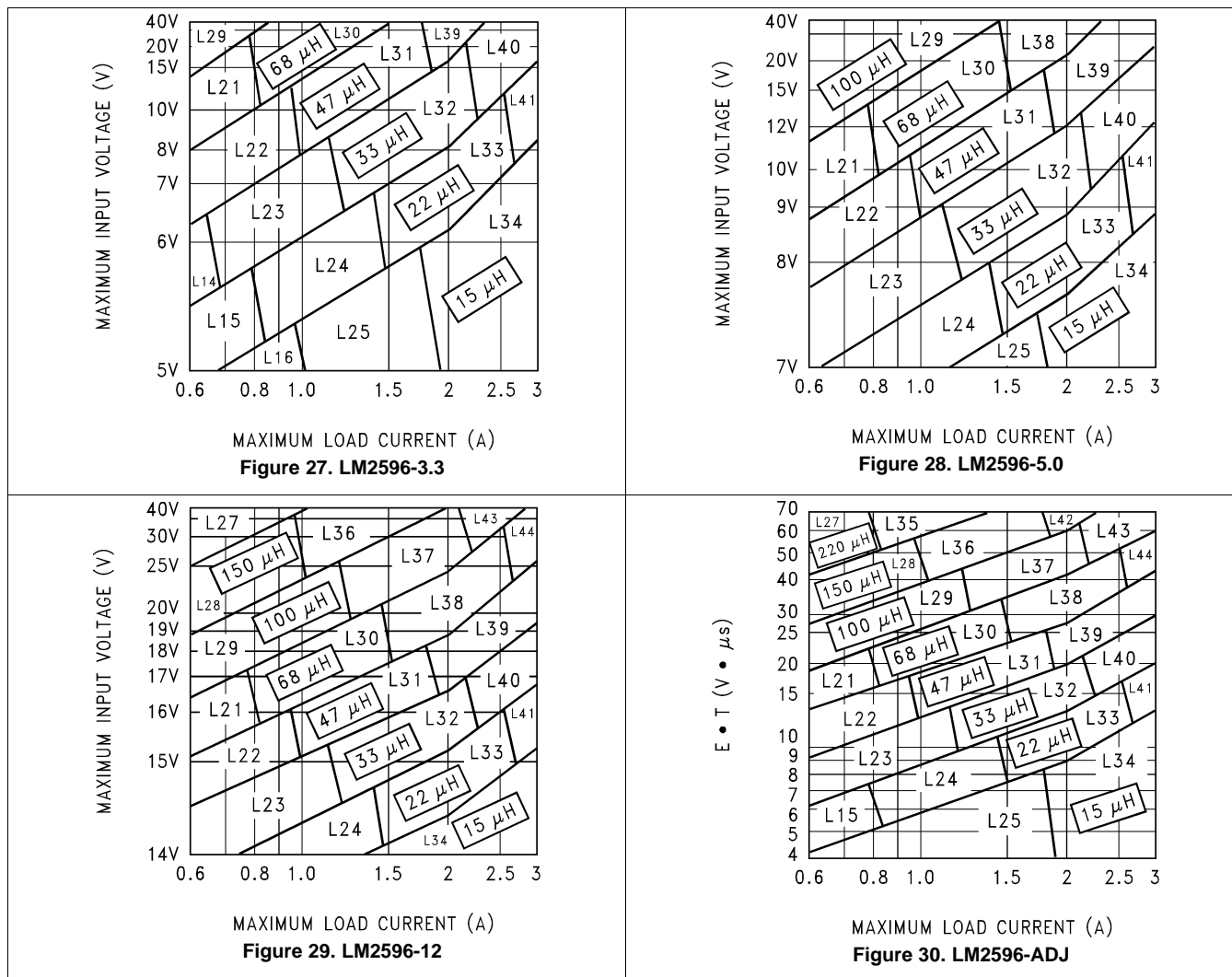
The inductors listed in the selection chart include ferrite E-core construction for Schottky, ferrite bobbin core for Renco and Coilcraft, and powdered iron toroid for Pulse Engineering.

Exceeding an inductor's maximum current rating may cause the inductor to overheat because of the copper wire losses, or the core may saturate. If the inductor begins to saturate, the inductance decreases rapidly and the inductor begins to look mainly resistive (the DC resistance of the winding). This can cause the switch current to rise very rapidly and force the switch into a cycle-by-cycle current limit, thus reducing the DC output load current. This can also result in overheating of the inductor or the LM2596. Different inductor types have different saturation characteristics, so consider this when selecting an inductor.

The inductor manufacturer's data sheets include current and energy limits to avoid inductor saturation.

For continuous mode operation, see the inductor selection graphs in [Figure 27](#) through [Figure 30](#).

**Application Information (continued)**



**Table 1. Inductor Manufacturers Part Numbers**

	INDUCTANCE (μH)	CURRENT (A)	SCHOTTKY		RENCO		PULSE ENGINEERING		COILCRAFT
			THROUGH-HOLE	SURFACE-MOUNT	THROUGH-HOLE	SURFACE-MOUNT	THROUGH-HOLE	SURFACE-MOUNT	SURFACE-MOUNT
L15	22	0.99	67148350	67148460	RL-1284-22-43	RL1500-22	PE-53815	PE-53815-S	DO3308-223
L21	68	0.99	67144070	67144450	RL-5471-5	RL1500-68	PE-53821	PE-53821-S	DO3316-683
L22	47	1.17	67144080	67144460	RL-5471-6	—	PE-53822	PE-53822-S	DO3316-473
L23	33	1.40	67144090	67144470	RL-5471-7	—	PE-53823	PE-53823-S	DO3316-333
L24	22	1.70	67148370	67148480	RL-1283-22-43	—	PE-53824	PE-53825-S	DO3316-223
L25	15	2.10	67148380	67148490	RL-1283-15-43	—	PE-53825	PE-53824-S	DO3316-153
L26	330	0.80	67144100	67144480	RL-5471-1	—	PE-53826	PE-53826-S	DO5022P-334
L27	220	1.00	67144110	67144490	RL-5471-2	—	PE-53827	PE-53827-S	DO5022P-224
L28	150	1.20	67144120	67144500	RL-5471-3	—	PE-53828	PE-53828-S	DO5022P-154
L29	100	1.47	67144130	67144510	RL-5471-4	—	PE-53829	PE-53829-S	DO5022P-104
L30	68	1.78	67144140	67144520	RL-5471-5	—	PE-53830	PE-53830-S	DO5022P-683
L31	47	2.20	67144150	67144530	RL-5471-6	—	PE-53831	PE-53831-S	DO5022P-473

**Application Information (continued)**
**Table 1. Inductor Manufacturers Part Numbers (continued)**

	INDUCTANCE ( $\mu$ H)	CURRENT (A)	SCHOTTKY		RENCO		PULSE ENGINEERING		COILCRAFT
			THROUGH- HOLE	SURFACE- MOUNT	THROUGH- HOLE	SURFACE- MOUNT	THROUGH- HOLE	SURFACE- MOUNT	SURFACE- MOUNT
L32	33	2.50	67144160	67144540	RL-5471-7	—	PE-53932	PE-53932-S	DO5022P-333
L33	22	3.10	67148390	67148500	RL-1283-22-43	—	PE-53933	PE-53933-S	DO5022P-223
L34	15	3.40	67148400	67148790	RL-1283-15-43	—	PE-53934	PE-53934-S	DO5022P-153
L35	220	1.70	67144170	—	RL-5473-1	—	PE-53935	PE-53935-S	—
L36	150	2.10	67144180	—	RL-5473-4	—	PE-54036	PE-54036-S	—
L37	100	2.50	67144190	—	RL-5472-1	—	PE-54037	PE-54037-S	—
L38	68	3.10	67144200	—	RL-5472-2	—	PE-54038	PE-54038-S	—
L39	47	3.50	67144210	—	RL-5472-3	—	PE-54039	PE-54039-S	—
L40	33	3.50	67144220	67148290	RL-5472-4	—	PE-54040	PE-54040-S	—
L41	22	3.50	67144230	67148300	RL-5472-5	—	PE-54041	PE-54041-S	—
L42	150	2.70	67148410	—	RL-5473-4	—	PE-54042	PE-54042-S	—
L43	100	3.40	67144240	—	RL-5473-2	—	PE-54043		—
L44	68	3.40	67144250	—	RL-5473-3	—	PE-54044		—

**9.1.6 Output Voltage Ripple and Transients**

The output voltage of a switching power supply operating in the continuous mode will contain a sawtooth ripple voltage at the switcher frequency, and may also contain short voltage spikes at the peaks of the sawtooth waveform.

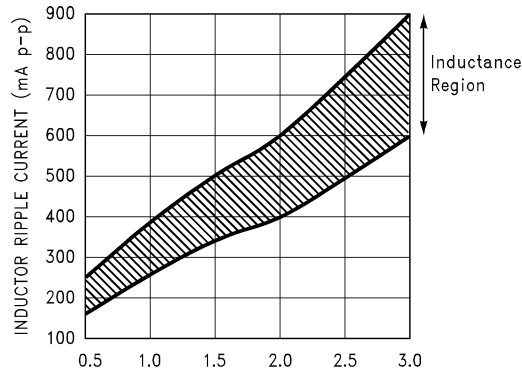
The output ripple voltage is a function of the inductor sawtooth ripple current and the ESR of the output capacitor. A typical output ripple voltage can range from approximately 0.5% to 3% of the output voltage. To obtain low ripple voltage, the ESR of the output capacitor must be low; however, exercise caution when using extremely low ESR capacitors because they can affect the loop stability, resulting in oscillation problems. TI recommends a post ripple filter if very low output ripple voltage is required (less than 20 mV) (see [Figure 32](#)). The inductance required is typically between 1  $\mu$ H and 5  $\mu$ H, with low DC resistance, to maintain good load regulation. A low ESR output filter capacitor is also required to assure good dynamic load response and ripple reduction. The ESR of this capacitor may be as low as desired, because it is out of the regulator feedback loop. [Figure 22](#) shows a typical output ripple voltage, with and without a post ripple filter.

When observing output ripple with a scope, it is essential that a short, low inductance scope probe ground connection be used. Most scope probe manufacturers provide a special probe terminator which is soldered onto the regulator board, preferably at the output capacitor. This provides a very short scope ground, thus eliminating the problems associated with the 3-inch ground lead normally provided with the probe, and provides a much cleaner and more accurate picture of the ripple voltage waveform.

The voltage spikes are caused by the fast switching action of the output switch and the diode, the parasitic inductance of the output filter capacitor, and its associated wiring. To minimize these voltage spikes, the output capacitor should be designed for switching regulator applications, and the lead lengths must be kept very short. Wiring inductance, stray capacitance, as well as the scope probe used to evaluate these transients, all contribute to the amplitude of these spikes.

When a switching regulator is operating in the continuous mode, the inductor current waveform ranges from a triangular to a sawtooth type of waveform (depending on the input voltage). For a given input and output voltage, the peak-to-peak amplitude of this inductor current waveform remains constant. As the load current increases or decreases, the entire sawtooth current waveform also rises and falls. The average value (or the center) of this current waveform is equal to the DC load current.

If the load current drops to a low enough level, the bottom of the sawtooth current waveform reaches zero, and the switcher smoothly changes from a continuous to a discontinuous mode of operation. Most switcher designs (regardless of how large the inductor value is) is forced to run discontinuous if the output is lightly loaded. This is a perfectly acceptable mode of operation.



**Figure 31. Peak-to-Peak Inductor Ripple Current vs Load Current**

In a switching regulator design, knowing the value of the peak-to-peak inductor ripple current ( $\Delta I_{IND}$ ) can be useful for determining a number of other circuit parameters. Parameters such as peak inductor or peak switch current, minimum load current before the circuit becomes discontinuous, output ripple voltage, and output capacitor ESR can all be calculated from the peak-to-peak  $\Delta I_{IND}$ . When the inductor nomographs in Figure 27 through Figure 30 are used to select an inductor value, the peak-to-peak inductor ripple current can immediately be determined. Figure 31 shows the range of ( $\Delta I_{IND}$ ) that can be expected for different load currents. Figure 31 also shows how the peak-to-peak inductor ripple current ( $\Delta I_{IND}$ ) changes as you go from the lower border to the upper border (for a given load current) within an inductance region. The upper border represents a higher input voltage, while the lower border represents a lower input voltage.

These curves are only correct for continuous mode operation, and only if the inductor selection guides are used to select the inductor value.

Consider the following example:

$V_{OUT} = 5\text{ V}$ , maximum load current of 2.5 A

$V_{IN} = 12\text{ V}$ , nominal, varying between 10 V and 16 V.

The selection guide in Figure 28 shows that the vertical line for a 2.5-A load current and the horizontal line for the 12-V input voltage intersect approximately midway between the upper and lower borders of the 33- $\mu\text{H}$  inductance region. A 33- $\mu\text{H}$  inductor allows a peak-to-peak inductor current ( $\Delta I_{IND}$ ), which is a percentage of the maximum load current, to flow. In Figure 31, follow the 2.5-A line approximately midway into the inductance region, and read the peak-to-peak inductor ripple current ( $\Delta I_{IND}$ ) on the left hand axis (approximately 620 mA p-p).

As the input voltage increases to 16 V, approaching the upper border of the inductance region, the inductor ripple current increases. Figure 31 shows that for a load current of 2.5 A, the peak-to-peak inductor ripple current ( $\Delta I_{IND}$ ) is 620 mA with 12  $V_{IN}$ , and can range from 740 mA at the upper border (16  $V_{IN}$ ) to 500 mA at the lower border (10  $V_{IN}$ ).

Once the  $\Delta I_{IND}$  value is known, use these equations to calculate additional information about the switching regulator circuit.

1. Peak Inductor or peak switch current  $= \left( I_{LOAD} + \frac{\Delta I_{IND}}{2} \right) = \left( 2.5\text{A} + \frac{0.62}{2} \right) = 2.81\text{A}$
2. Minimum load current before the circuit becomes discontinuous  $= \frac{\Delta I_{IND}}{2} = \frac{0.62}{2} = 0.31\text{A}$
3. Output Ripple Voltage  $= (\Delta I_{IND}) \times (\text{ESR of } C_{OUT}) = 0.62\text{ A} \times 0.1\ \Omega = 62\text{ mVp-p}$
- 4.

$$\begin{aligned} \text{ESR of } C_{OUT} &= \frac{\text{Output Ripple Voltage } (\Delta V_{OUT})}{\Delta I_{IND}} \\ &= \frac{0.062\text{V}}{0.62\text{A}} = 0.1\ \Omega \end{aligned}$$

### 9.1.7 Open-Core Inductors

Another possible source of increased output ripple voltage or unstable operation is from an open-core inductor. Ferrite bobbin or stick inductors have magnetic lines of flux flowing through the air from one end of the bobbin to the other end. These magnetic lines of flux will induce a voltage into any wire or PCB copper trace that comes within the inductor's magnetic field. The strength of the magnetic field, the orientation and location of the PCB copper trace to the magnetic field, and the distance between the copper trace and the inductor determine the amount of voltage generated in the copper trace. Another way of looking at this inductive coupling is to consider the PCB copper trace as one turn of a transformer (secondary) with the inductor winding as the primary. Many millivolts can be generated in a copper trace located near an open-core inductor, which can cause stability problems or high output ripple voltage problems.

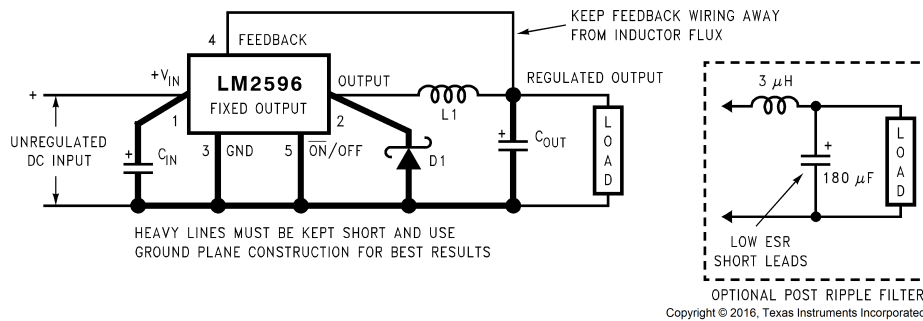
If unstable operation is seen, and an open-core inductor is used, it is possible that the location of the inductor with respect to other PC traces may be the problem. To determine if this is the problem, temporarily raise the inductor away from the board by several inches and then check circuit operation. If the circuit now operates correctly, then the magnetic flux from the open core inductor is causing the problem. Substituting a closed core inductor such as a torroid or E-core will correct the problem, or re-arranging the PC layout may be necessary. Magnetic flux cutting the IC device ground trace, feedback trace, or the positive or negative traces of the output capacitor should be minimized.

Sometimes, placing a trace directly beneath a bobbin inductor will provide good results, provided it is exactly in the center of the inductor (because the induced voltages cancel themselves out). However, problems could arise if the trace is off center one direction or the other. If flux problems are present, even the direction of the inductor winding can make a difference in some circuits.

This discussion on open core inductors is not to frighten users, but to alert users on what kind of problems to watch out for. Open-core bobbin or *stick* inductors are an inexpensive, simple way of making a compact, efficient inductor, and they are used by the millions in many different applications.

## 9.2 Typical Applications

### 9.2.1 LM2596 Fixed Output Series Buck Regulator



- C<sub>IN</sub> — 470-μF, 50-V, Aluminum Electrolytic Nichicon *PL Series*
- C<sub>OUT</sub> — 220-μF, 25-V Aluminum Electrolytic, Nichicon *PL Series*
- D1 — 5-A, 40-V Schottky Rectifier, 1N5825
- L1 — 68 μH, L38

Figure 32. Fixed Output Voltage Version

#### 9.2.1.1 Design Requirements

Table 2 lists the design parameters for this example.

Table 2. Design Parameters

PARAMETER	EXAMPLE VALUE
Regulated Output Voltage (3.3 V, 5 V or 12 V), V <sub>OUT</sub>	5 V
Maximum DC Input Voltage, V <sub>IN(max)</sub>	12 V
Maximum Load Current, I <sub>LOAD(max)</sub>	3 A

### 9.2.1.2 Detailed Design Procedure

#### 9.2.1.2.1 Inductor Selection (L1)

1. Select the correct inductor value selection guide from [Figure 27](#), [Figure 28](#), or [Figure 29](#) (output voltages of 3.3V, 5V, or 12V respectively). Use the inductor selection guide for the 5-V version shown in [Figure 28](#).
2. From the inductor value selection guide, identify the inductance region intersected by the maximum input voltage line and the maximum load current line. Each region is identified by an inductance value and an inductor code (LXX). From the inductor value selection guide shown in [Figure 28](#), the inductance region intersected by the 12-V horizontal line and the 3-A vertical line is 33  $\mu$ H, and the inductor code is L40.
3. Select an appropriate inductor from the four manufacturer's part numbers listed in [Table 1](#). The inductance value required is 33  $\mu$ H. See row L40 of [Table 1](#) and choose an inductor part number from any of the manufacturers shown. In most instances, both through-hole and surface-mount inductors are available.

#### 9.2.1.2.2 Output Capacitor Selection (C<sub>OUT</sub>)

1. In the majority of applications, low ESR (Equivalent Series Resistance) electrolytic capacitors between 82  $\mu$ F and 820  $\mu$ F and low ESR solid tantalum capacitors between 10  $\mu$ F and 470  $\mu$ F provide the best results. This capacitor must be placed close to the IC using short capacitor leads and short copper traces. Do not use capacitors larger than 820  $\mu$ F .

#### NOTE

For additional information, see section on output capacitors in [Table 3](#).

2. To simplify the capacitor selection procedure, see [Table 3](#) for quick design component selection. This table contains different input voltages, output voltages, and load currents, and lists various inductors and output capacitors that will provide the best design solutions.

From [Table 3](#), locate the 5-V output voltage section. In the load current column, choose the load current line that is closest to the current required for the application; for this example, use the 3-A line. In the maximum input voltage column, select the line that covers the input voltage required for the application; in this example, use the 15-V line. The rest of the line shows recommended inductors and capacitors that will provide the best overall performance.

**Table 3. LM2596 Fixed Voltage Quick Design Component Selection Table**

CONDITIONS			INDUCTOR		OUTPUT CAPACITOR			
OUTPUT VOLTAGE (V)	LOAD CURRENT (A)	MAX INPUT VOLTAGE (V)	INDUCTANCE ( $\mu$ H)	INDUCTOR (#)	THROUGH-HOLE ELECTROLYTIC		SURFACE-MOUNT TANTALUM	
					PANASONIC HFQ SERIES ( $\mu$ F/V)	NICHICON PL SERIES ( $\mu$ F/V)	AVX TPS SERIES ( $\mu$ F/V)	SPRAGUE 595D SERIES ( $\mu$ F/V)
3.3	3	5	22	L41	470/25	560/16	330/6.3	390/6.3
		7	22	L41	560/35	560/35	330/6.3	390/6.3
		10	22	L41	680/35	680/35	330/6.3	390/6.3
		40	33	L40	560/35	470/35	330/6.3	390/6.3
	2	6	22	L33	470/25	470/35	330/6.3	390/6.3
		10	33	L32	330/35	330/35	330/6.3	390/6.3
		40	47	L39	330/35	270/50	220/10	330/10
5	3	8	22	L41	470/25	560/16	220/10	330/10
		10	22	L41	560/25	560/25	220/10	330/10
		15	33	L40	330/35	330/35	220/10	330/10
		40	47	L39	330/35	270/35	220/10	330/10
	2	9	22	L33	470/25	560/16	220/10	330/10
		20	68	L38	180/35	180/35	100/10	270/10
		40	68	L38	180/35	180/35	100/10	270/10

**Table 3. LM2596 Fixed Voltage Quick Design Component Selection Table (continued)**

CONDITIONS			INDUCTOR		OUTPUT CAPACITOR			
					THROUGH-HOLE ELECTROLYTIC		SURFACE-MOUNT TANTALUM	
OUTPUT VOLTAGE (V)	LOAD CURRENT (A)	MAX INPUT VOLTAGE (V)	INDUCTANCE (μH)	INDUCTOR (#)	PANASONIC HFQ SERIES (μF/V)	NICHICON PL SERIES (μF/V)	AVX TPS SERIES (μF/V)	SPRAGUE 595D SERIES (μF/V)
12	3	15	22	L41	470/25	470/25	100/16	180/16
		18	33	L40	330/25	330/25	100/16	180/16
		30	68	L44	180/25	180/25	100/16	120/20
		40	68	L44	180/35	180/35	100/16	120/20
	2	15	33	L32	330/25	330/25	100/16	180/16
		20	68	L38	180/25	180/25	100/16	120/20
		40	150	L42	82/25	82/25	68/20	68/25

The capacitor list contains both through-hole electrolytic and surface-mount tantalum capacitors from four different capacitor manufacturers. TI recommends that both the manufacturers and the manufacturer's series that are listed in [Table 3](#).

In this example aluminum electrolytic capacitors from several different manufacturers are available with the range of ESR numbers required.

- 330-μF, 35-V Panasonic HFQ Series
- 330-μF, 35-V Nichicon PL Series

3. The capacitor voltage rating for electrolytic capacitors should be at least 1.5 times greater than the output voltage, and often require much higher voltage ratings to satisfy the low ESR requirements for low output ripple voltage.

For a 5-V output, a capacitor voltage rating of at least 7.5 V is required. But even a low ESR, switching grade, 220-μF, 10-V aluminum electrolytic capacitor would exhibit approximately 225 mΩ of ESR (see [Figure 24](#) for the ESR vs voltage rating). This amount of ESR would result in relatively high output ripple voltage. To reduce the ripple to 1% or less of the output voltage, a capacitor with a higher value or with a higher voltage rating (lower ESR) must be selected. A 16-V or 25-V capacitor will reduce the ripple voltage by approximately half.

**9.2.1.2.3 Catch Diode Selection (D1)**

1. The catch diode current rating must be at least 1.3 times greater than the maximum load current. Also, if the power supply design must withstand a continuous output short, the diode must have a current rating equal to the maximum current limit of the LM2596. The most stressful condition for this diode is an overload or shorted output condition. See [Table 4](#). In this example, a 5-A, 20-V, 1N5823 Schottky diode will provide the best performance, and will not be overstressed even for a shorted output.

**Table 4. Diode Selection Table**

VR	3-A DIODES				4-A TO 6-A DIODES			
	SURFACE-MOUNT		THROUGH-HOLE		SURFACE-MOUNT		THROUGH-HOLE	
	SCHOTTKY	ULTRA FAST RECOVERY	SCHOTTKY	ULTRA FAST RECOVERY	SCHOTTKY	ULTRA FAST RECOVERY	SCHOTTKY	ULTRA FAST RECOVERY
20 V	SK32	All of these diodes are rated to at least 50V.	1N5820	All of these diodes are rated to at least 50V.		All of these diodes are rated to at least 50V.	SR502	All of these diodes are rated to at least 50V.
			SR302				1N5823	
			MBR320				SB520	
30 V	30WQ03		1N5821					
	SK33		MBR330		50WQ03		SR503	
			31DQ03				1N5824	
40 V	SK34		1N5822			SB530		
			SR304	50WQ04	SR504			
		MBRS340	MBR340		1N5825			
	30WQ04	MURS320	31DQ04	MUR320		MURS620	SB540	MUR620
50 V	SK35	30WF10	SR305			50WF10		HER601
or	MBRS360		MBR350		50WQ05		SB550	
More	30WQ05		31DQ05				50SQ080	



2. The reverse voltage rating of the diode must be at least 1.25 times the maximum input voltage.
3. This diode must be fast (short reverse recovery time) and must be placed close to the LM2596 using short leads and short-printed circuit traces. Because of their fast switching speed and low forward voltage drop, Schottky diodes provide the best performance and efficiency, and must be the first choice, especially in low output voltage applications. Ultra-fast recovery, or high-efficiency rectifiers also provide good results. Ultra-fast recovery diodes typically have reverse recovery times of 50 ns or less. Rectifiers such as the 1N5400 series must not be used because they are too slow.

#### 9.2.1.2.4 Input Capacitor ( $C_{IN}$ )

A low ESR aluminum or tantalum bypass capacitor is required between the input pin and ground pin to prevent large voltage transients from appearing at the input. This capacitor must be placed close to the IC using short leads. In addition, the RMS current rating of the input capacitor should be selected to be at least  $\frac{1}{2}$  the DC load current. The capacitor manufacturers data sheet must be checked to assure that this current rating is not exceeded. [Figure 23](#) shows typical RMS current ratings for several different aluminum electrolytic capacitor values.

For an aluminum electrolytic, the capacitor voltage rating must be approximately 1.5 times the maximum input voltage. Exercise caution if solid tantalum capacitors are used (see [Input Capacitor \( \$C\_{IN}\$ \)](#)). The tantalum capacitor voltage rating should be 2 times the maximum input voltage and TI recommends that they be surge current tested by the manufacturer.

Use caution when using ceramic capacitors for input bypassing, because it may cause severe ringing at the  $V_{IN}$  pin.

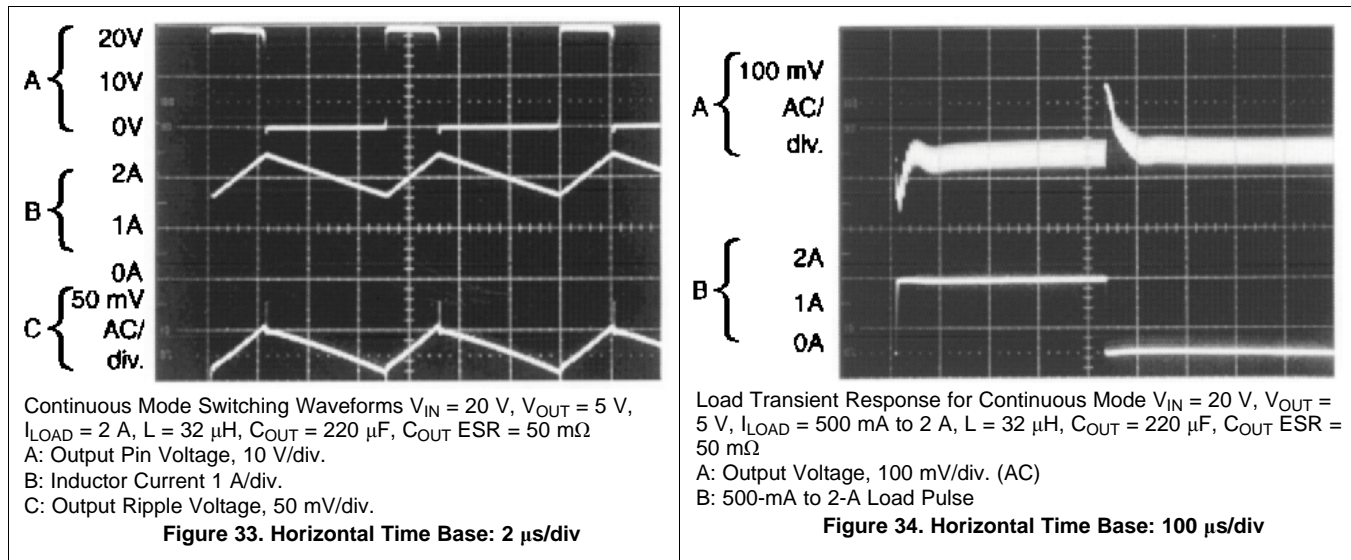
The important parameters for the Input capacitor are the input voltage rating and the RMS current rating. With a nominal input voltage of 12 V, an aluminum electrolytic capacitor with a voltage rating greater than 18 V ( $1.5 \times V_{IN}$ ) is necessary. The next higher capacitor voltage rating is 25 V.

The RMS current rating requirement for the input capacitor in a buck regulator is approximately  $\frac{1}{2}$  the DC load current. In this example, with a 3-A load, a capacitor with a RMS current rating of at least 1.5 A is required. [Figure 23](#) can be used to select an appropriate input capacitor. From the curves, locate the 35-V line and note which capacitor values have RMS current ratings greater than 1.5 A. A 680- $\mu$ F, 35-V capacitor could be used.

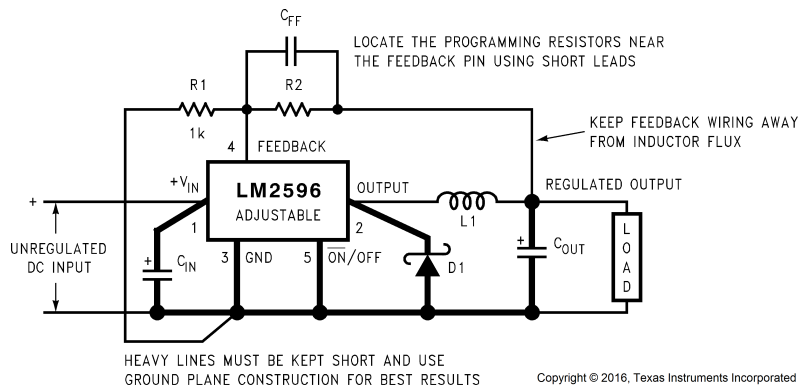
For a through-hole design, a 680- $\mu$ F, 35-V electrolytic capacitor (Panasonic HFQ series or Nichicon PL series or equivalent) would be adequate. Other types or other manufacturers' capacitors can be used provided the RMS ripple current ratings are adequate.

For surface-mount designs, solid tantalum capacitors can be used, but exercise caution with regard to the capacitor surge current rating (see [Input Capacitor \( \$C\_{IN}\$ \)](#) in this data sheet). The TPS series available from AVX, and the 593D series from Sprague are both surge current tested.

9.2.1.3 Application Curves



9.2.2 LM2596 Adjustable Output Series Buck Regulator



$$V_{OUT} = V_{REF} \left( 1 + \frac{R_2}{R_1} \right)$$

where  $V_{REF} = 1.23\text{ V}$

$$R_2 = R_1 \left( \frac{V_{OUT}}{V_{REF}} - 1 \right)$$

Select  $R_1$  to be approximately 1 k $\Omega$ , use a 1% resistor for best stability.

$C_{IN}$  — 470- $\mu\text{F}$ , 50-V, Aluminum Electrolytic Nichicon *PL Series*

$C_{OUT}$  — 220- $\mu\text{F}$ , 35-V Aluminum Electrolytic, Nichicon *PL Series*

D1 — 5-A, 40-V Schottky Rectifier, 1N5825

L1 — 68  $\mu\text{H}$ , L38

R1 — 1 k $\Omega$ , 1%

$C_{FF}$  — See [Feedforward Capacitor \( \$C\_{FF}\$ \)](#)

Figure 35. Adjustable Output Voltage Version

### 9.2.2.1 Design Requirements

Table 5 lists the design parameters for this example.

**Table 5. Design Parameters**

PARAMETER	EXAMPLE VALUE
Regulated output voltage (3.3V, 5V or 12V), $V_{OUT}$	20 V
Maximum DC input voltage, $V_{IN(max)}$	28 V
Maximum load current, $I_{LOAD(max)}$	3 A
Switching frequency, F	Fixed at a nominal 150 kHz

### 9.2.2.2 Detailed Design Procedure

#### 9.2.2.2.1 Programming Output Voltage

Select  $R_1$  and  $R_2$ , as shown in Table 6

Use Equation 1 to select the appropriate resistor values.

$$V_{OUT} = V_{REF} \left( 1 + \frac{R_2}{R_1} \right) \quad \text{where } V_{REF} = 1.23V \quad (1)$$

Select a value for  $R_1$  between 240  $\Omega$  and 1.5 k $\Omega$ . The lower resistor values minimize noise pickup in the sensitive feedback pin. (For the lowest temperature coefficient and the best stability with time, use 1% metal film resistors.). Calculate  $R_2$  with Equation 2.

$$R_2 = R_1 \left( \frac{V_{OUT}}{V_{REF}} - 1 \right) \quad (2)$$

Select  $R_1$  to be 1 k $\Omega$ , 1%. Solve for  $R_2$  in Equation 3.

$$R_2 = R_1 \left( \frac{V_{OUT}}{V_{REF}} - 1 \right) = 1k \left( \frac{20V}{1.23V} - 1 \right) \quad (3)$$

$R_2 = 1k (16.26 - 1) = 15.26k$ , closest 1% value is 15.4 k $\Omega$ .

$R_2 = 15.4$  k $\Omega$ .

#### 9.2.2.2.2 Inductor Selection (L1)

1. Calculate the inductor Volt • microsecond constant  $E \times T$  ( $V \times \mu s$ ), with Equation 4:

$$E \times T = (V_{IN} - V_{OUT} - V_{SAT}) \cdot \frac{V_{OUT} + V_D}{V_{IN} - V_{SAT} + V_D} \cdot \frac{1000}{150 \text{ kHz}} (V \cdot \mu s)$$

where

- $V_{SAT}$  = internal switch saturation voltage = 1.16 V
- $V_D$  = diode forward voltage drop = 0.5 V

Calculate the inductor Volt • microsecond constant

( $E \times T$ ),

$$E \times T = (28 - 20 - 1.16) \cdot \frac{20 + 0.5}{28 - 1.16 + 0.5} \cdot \frac{1000}{150} (V \cdot \mu s)$$

$$E \times T = (6.84) \cdot \frac{20.5}{27.34} \cdot 6.67 (V \cdot \mu s) = 34.2 (V \cdot \mu s) \quad (5)$$

2. Use the  $E \times T$  value from the previous formula and match it with the  $E \times T$  number on the vertical axis of the Inductor Value Selection Guide shown in Figure 30.

$$E \times T = 34.2 (V \times \mu s)$$

3. On the horizontal axis, select the maximum load current.

$$I_{LOAD(max)} = 3 \text{ A}$$

4. Identify the inductance region intersected by the  $E \times T$  value and the maximum load current value. Each region is identified by an inductance value and an inductor code (LXX). From the inductor value selection guide shown in Figure 30, the inductance region intersected by the 34 ( $V \cdot \mu s$ ) horizontal line and the 3-A

vertical line is 47  $\mu\text{H}$ , and the inductor code is L39.

5. Select an appropriate inductor from the manufacturers' part numbers listed in [Table 1](#). From the table in [Table 1](#), locate line L39, and select an inductor part number from the list of manufacturers part numbers.

#### 9.2.2.2.3 Output Capacitor Selection ( $C_{\text{OUT}}$ )

1. In the majority of applications, low ESR electrolytic or solid tantalum capacitors between 82  $\mu\text{F}$  and 820  $\mu\text{F}$  provide the best results. This capacitor must be placed close to the IC using short capacitor leads and short copper traces. Do not use capacitors larger than 820  $\mu\text{F}$ .

#### NOTE

For additional information, see section on output capacitors in [Output Capacitor \( \$C\_{\text{OUT}}\$ \)](#) section.

2. To simplify the capacitor selection procedure, see [Table 6](#) for a quick design guide. This table contains different output voltages, and lists various output capacitors that will provide the best design solutions.

From [Table 6](#), locate the output voltage column. From that column, locate the output voltage closest to the output voltage in your application. In this example, select the 24-V line. Under the [Output Capacitor \( \$C\_{\text{OUT}}\$ \)](#) section, select a capacitor from the list of through-hole electrolytic or surface-mount tantalum types from four different capacitor manufacturers. TI recommends that both the manufacturers and the manufacturers' series that are listed in [Table 6](#) be used.

In this example, through hole aluminum electrolytic capacitors from several different manufacturers are available.

- 220- $\mu\text{F}$ , 35-V Panasonic HFQ Series
- 150- $\mu\text{F}$ , 35-V Nichicon PL Series

3. The capacitor voltage rating must be at least 1.5 times greater than the output voltage, and often much higher voltage ratings are required to satisfy the low ESR requirements required for low output ripple voltage.

For a 20-V output, a capacitor rating of at least 30 V is required. In this example, either a 35-V or 50-V capacitor would work. A 35-V rating was chosen, although a 50-V rating could also be used if a lower output ripple voltage is required.

Other manufacturers or other types of capacitors may also be used, provided the capacitor specifications (especially the 100-kHz ESR) closely match the types listed in [Table 6](#). Refer to the capacitor manufacturers data sheet for this information.

#### 9.2.2.2.4 Feedforward Capacitor ( $C_{\text{FF}}$ )

See [Table 6](#).

For output voltages greater than approximately 10 V, an additional capacitor is required. The compensation capacitor is typically between 100 pF and 33 nF, and is wired in parallel with the output voltage setting resistor,  $R_2$ . It provides additional stability for high output voltages, low input or output voltages, or very low ESR output capacitors, such as solid tantalum capacitors. Calculate the value for  $C_{\text{FF}}$  with [Equation 6](#):

$$C_{\text{FF}} = \frac{1}{31 \times 10^3 \times R_2} \quad (6)$$

This capacitor type can be ceramic, plastic, silver mica, and so forth. Because of the unstable characteristics of ceramic capacitors made with Z5U material, they are not recommended.

[Table 6](#) contains feedforward capacitor values for various output voltages. In this example, a 560-pF capacitor is required.

**Table 6. Output Capacitor and Feedforward Capacitor Selection Table**

OUTPUT VOLTAGE (V)	THROUGH-HOLE OUTPUT CAPACITOR			SURFACE-MOUNT OUTPUT CAPACITOR		
	PANASONIC HFQ SERIES ( $\mu\text{F}/\text{V}$ )	NICHICON PL SERIES ( $\mu\text{F}/\text{V}$ )	FEEDFORWARD CAPACITOR	AVX TPS SERIES ( $\mu\text{F}/\text{V}$ )	SPRAGUE 595D SERIES ( $\mu\text{F}/\text{V}$ )	FEEDFORWARD CAPACITOR
2	820/35	820/35	33 nF	330/6.3	470/4	33 nF
4	560/35	470/35	10 nF	330/6.3	390/6.3	10 nF

**Table 6. Output Capacitor and Feedforward Capacitor Selection Table (continued)**

OUTPUT VOLTAGE (V)	THROUGH-HOLE OUTPUT CAPACITOR			SURFACE-MOUNT OUTPUT CAPACITOR		
	PANASONIC HFQ SERIES ( $\mu\text{F/V}$ )	NICHICON PL SERIES ( $\mu\text{F/V}$ )	FEEDFORWARD CAPACITOR	AVX TPS SERIES ( $\mu\text{F/V}$ )	SPRAGUE 595D SERIES ( $\mu\text{F/V}$ )	FEEDFORWARD CAPACITOR
6	470/25	470/25	3.3 nF	220/10	330/10	3.3 nF
9	330/25	330/25	1.5 nF	100/16	180/16	1.5 nF
12	330/25	330/25	1 nF	100/16	180/16	1 nF
15	220/35	220/35	680 pF	68/20	120/20	680 pF
24	220/35	150/35	560 pF	33/25	33/25	220 pF
28	100/50	100/50	390 pF	10/35	15/50	220 pF

#### 9.2.2.2.5 Catch Diode Selection (D1)

1. The catch diode current rating must be at least 1.3 times greater than the maximum load current. Also, if the power supply design must withstand a continuous output short, the diode must have a current rating equal to the maximum current limit of the LM2596. The most stressful condition for this diode is an overload or shorted output condition. See [Table 4](#). Schottky diodes provide the best performance, and in this example a 5-A, 40-V, 1N5825 Schottky diode would be a good choice. The 5-A diode rating is more than adequate and will not be overstressed even for a shorted output.
2. The reverse voltage rating of the diode must be at least 1.25 times the maximum input voltage.
3. This diode must be fast (short reverse recovery time) and must be placed close to the LM2596 using short leads and short-printed circuit traces. Because of their fast switching speed and low forward voltage drop, Schottky diodes provide the best performance and efficiency, and must be the first choice, especially in low output voltage applications. Ultra-fast recovery or high-efficiency rectifiers are also good choices, but some types with an abrupt turnoff characteristic may cause instability or EMI problems. Ultra-fast recovery diodes typically have reverse recovery times of 50 ns or less. Rectifiers such as the 1N4001 series must not be used because they are too slow.

#### 9.2.2.2.6 Input Capacitor ( $C_{IN}$ )

A low ESR aluminum or tantalum bypass capacitor is required between the input pin and ground to prevent large voltage transients from appearing at the input. In addition, the RMS current rating of the input capacitor should be selected to be at least  $\frac{1}{2}$  the DC load current. The capacitor manufacturers data sheet must be checked to assure that this current rating is not exceeded. [Figure 23](#) shows typical RMS current ratings for several different aluminum electrolytic capacitor values.

This capacitor must be placed close to the IC using short leads and the voltage rating must be approximately 1.5 times the maximum input voltage.

If solid tantalum input capacitors are used, TI recommends that they be surge current tested by the manufacturer.

Use caution when using a high dielectric constant ceramic capacitor for input bypassing, because it may cause severe ringing at the  $V_{IN}$  pin.

The important parameters for the input capacitor are the input voltage rating and the RMS current rating. With a nominal input voltage of 28 V, an aluminum electrolytic capacitor with a voltage rating greater than 42 V ( $1.5 \times V_{IN}$ ) is required. Because the next higher capacitor voltage rating is 50 V, a 50-V capacitor must be used. The capacitor voltage rating of ( $1.5 \times V_{IN}$ ) is a conservative guideline, and can be modified somewhat if desired.

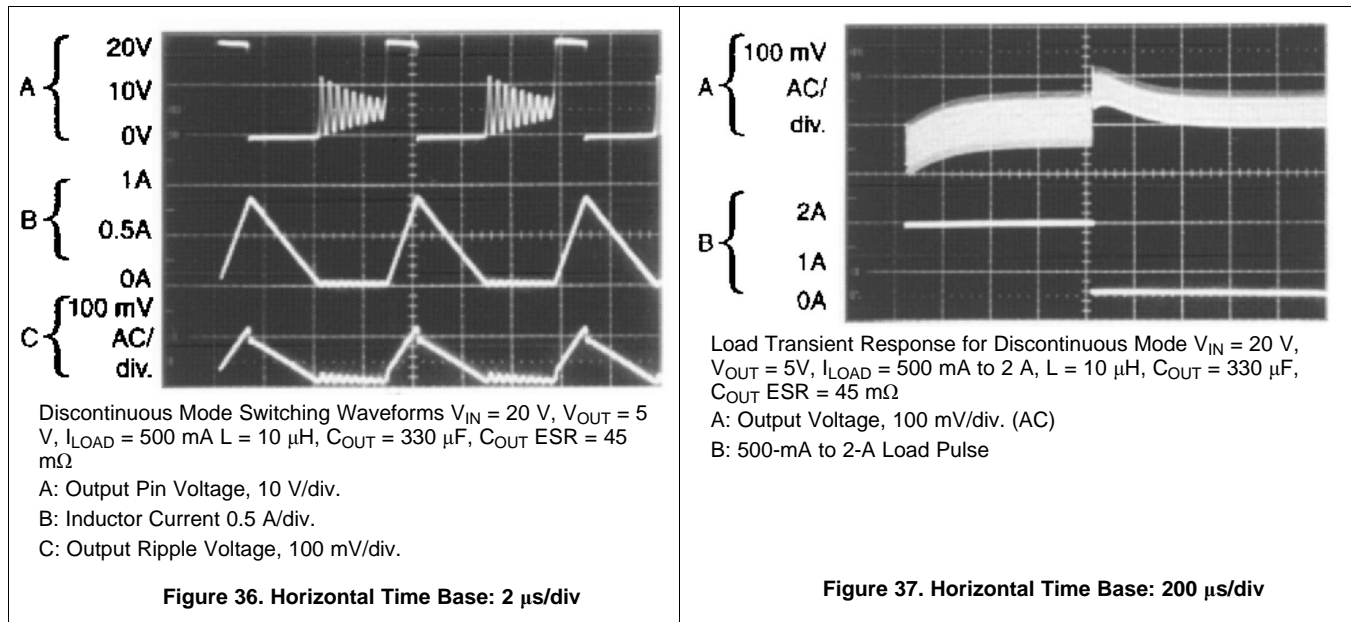
The RMS current rating requirement for the input capacitor of a buck regulator is approximately  $\frac{1}{2}$  the DC load current. In this example, with a 3-A load, a capacitor with a RMS current rating of at least 1.5 A is required.

[Figure 23](#) can be used to select an appropriate input capacitor. From the curves, locate the 50-V line and note which capacitor values have RMS current ratings greater than 1.5 A. Either a 470  $\mu\text{F}$  or 680  $\mu\text{F}$ , 50-V capacitor could be used.

For a through hole design, a 680- $\mu\text{F}$ , 50-V electrolytic capacitor (Panasonic HFQ series or Nichicon PL series or equivalent) would be adequate. Other types or other manufacturers' capacitors can be used provided the RMS ripple current ratings are adequate.

For surface mount designs, solid tantalum capacitors can be used, but exercise caution with regard to the capacitor surge current rating (see *Input Capacitor ( $C_{IN}$ )* in this data sheet). The TPS series available from AVX, and the 593D series from Sprague are both surge current tested.

### 9.2.2.3 Application Curves



## 10 Power Supply Recommendations

The LM2596 is designed to operate from an input voltage supply up to 40 V. This input supply must be well regulated and able to withstand maximum input current and maintain a stable voltage.

## 11 Layout

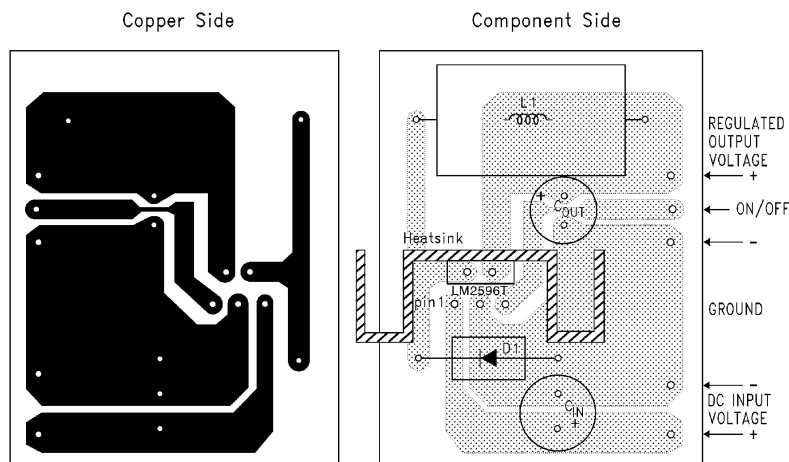
### 11.1 Layout Guidelines

As in any switching regulator, layout is very important. Rapidly switching currents associated with wiring inductance can generate voltage transients which can cause problems. For minimal inductance and ground loops, the wires indicated by heavy lines must be wide printed-circuit traces and must be kept as short as possible. For best results, external components must be placed as close to the switcher IC as possible using ground plane construction or single point grounding.

If open core inductors are used, take special care selecting the location and positioning of this type of inductor. Allowing the inductor flux to intersect sensitive feedback, IC groundpath and  $C_{OUT}$  wiring can cause problems.

When using the adjustable version, take special care selecting the location of the feedback resistors and the associated wiring. Physically place both resistors near the IC, and route the wiring away from the inductor, especially an open-core type of inductor (see [Open-Core Inductors](#) for more information).

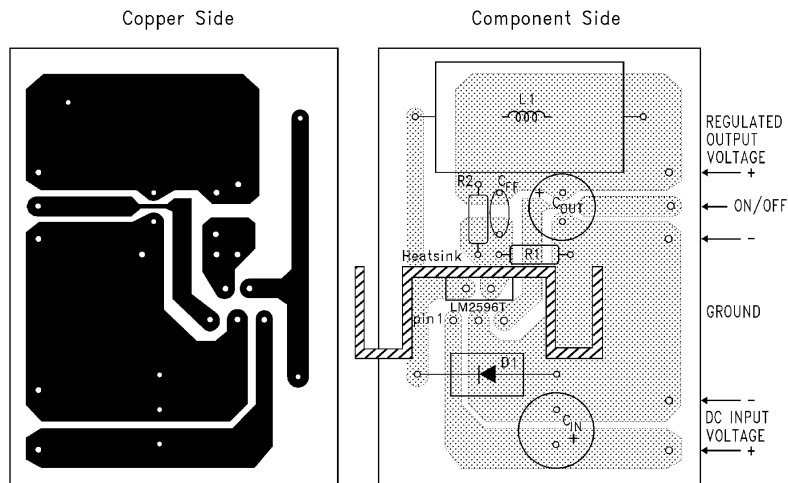
### 11.2 Layout Examples



$C_{IN}$  — 470- $\mu$ F, 50-V, Aluminum Electrolytic Panasonic, *HFQ Series*  
 $C_{OUT}$  — 330- $\mu$ F, 35-V, Aluminum Electrolytic Panasonic, *HFQ Series*  
D1 — 5-A, 40-V Schottky Rectifier, 1N5825  
L1 — 47- $\mu$ H, L39, Renco, Through Hole  
Thermalloy Heat Sink #7020

**Figure 38. Typical Through-Hole PCB Layout, Fixed Output (1x Size), Double-Sided**

Layout Examples (continued)



- $C_{IN}$ — 470- $\mu$ F, 50-V, Aluminum Electrolytic Panasonic, *HFQ Series*
- $C_{OUT}$ —220- $\mu$ F, 35-V Aluminum Electrolytic Panasonic, *HFQ Series*
- D1—5-A, 40-V Schottky Rectifier, 1N5825
- L1—47- $\mu$ H, L39, Renco, Through Hole
- $R_1$ —1 k $\Omega$ , 1%
- $R_2$ —Use formula in Design Procedure
- $C_{FF}$ —See [Table 6](#).
- Thermalloy Heat Sink #7020

Figure 39. Typical Through-Hole PCB Layout, Adjustable Output (1x Size), Double-Sided



### 11.3 Thermal Considerations

The LM2596 is available in two packages: a 7-pin TO-220 (T) and a 7-pin surface mount TO-263 (S).

The TO-220 package requires a heat sink under most conditions. The size of the heat sink depends on the input voltage, the output voltage, the load current and the ambient temperature. Figure 40 shows the LM2596T junction temperature rises above ambient temperature for a 3-A load and different input and output voltages. The data for these curves was taken with the LM2596T (TO-220 package) operating as a buck switching regulator in an ambient temperature of 25°C (still air). These temperature rise numbers are all approximate and there are many factors that can affect these temperatures. Higher ambient temperatures require more heat sinking.

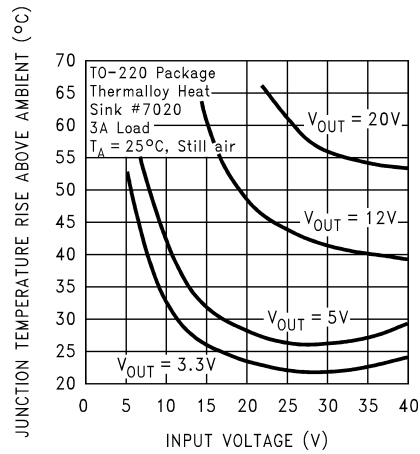
The TO-263 surface mount package tab is designed to be soldered to the copper on a printed-circuit board (PCB). The copper and the board are the heat sink for this package and the other heat producing components, such as the catch diode and inductor. The PCB copper area that the package is soldered to must be at least 0.4 in<sup>2</sup>, and ideally must have 2 or more square inches of 2-oz. (0.0028 in.) copper. Additional copper area improves the thermal characteristics, but with copper areas greater than approximately 6 in<sup>2</sup>, only small improvements in heat dissipation are realized. If further thermal improvements are required, TI recommends double-sided, multilayer PCB with large copper areas and airflow.

Figure 41 shows the LM2596S (TO-263 package) junction temperature rise above ambient temperature with a 2-A load for various input and output voltages. This data was taken with the circuit operating as a buck switching regulator with all components mounted on a PCB to simulate the junction temperature under actual operating conditions. This curve can be used for a quick check for the approximate junction temperature for various conditions, but be aware that there are many factors that can affect the junction temperature. When load currents higher than 2 A are used, double-sided or multilayer PCB with large copper areas or airflow might be required, especially for high ambient temperatures and high output voltages.

For the best thermal performance, wide copper traces and generous amounts of PCB copper must be used in the board layout. (One exception to this is the output (switch) pin, which should **not** have large areas of copper.) Large areas of copper provide the best transfer of heat (lower thermal resistance) to the surrounding air, and moving air lowers the thermal resistance even further.

Package thermal resistance and junction temperature rise numbers are all approximate, and there are many factors that will affect these numbers. Some of these factors include board size, shape, thickness, position, location, and even board temperature. Other factors are trace width, total printed-circuit copper area, copper thickness, single- or double-sided multilayer board, and the amount of solder on the board. The effectiveness of the PCB to dissipate heat also depends on the size, quantity, and spacing of other components on the board, as well as whether the surrounding air is still or moving. Furthermore, some of these components such as the catch diode will add heat to the PCB and the heat can vary as the input voltage changes. For the inductor, depending on the physical size, type of core material, and the DC resistance, it could either act as a heat sink taking heat away from the board, or it could add heat to the board.

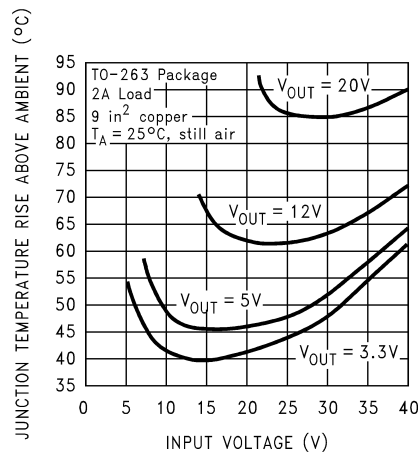
**Thermal Considerations (continued)**



**CIRCUIT DATA FOR TEMPERATURE RISE CURVE TO-220 PACKAGE (T)**

Capacitors	Through-hole electrolytic
Inductor	Through-hole, Renco
Diode	Through-hole, 5-A 40-V, Schottky
PCB	3-square inch, single-sided, 2-oz. copper (0.0028")

**Figure 40. Junction Temperature Rise, TO-220**



**CIRCUIT DATA FOR TEMPERATURE RISE CURVE TO-263 PACKAGE (S)**

Capacitors	Surface-mount tantalum, molded <i>D</i> size
Inductor	Surface-mount, Pulse Engineering, 68 $\mu\text{H}$
Diode	Surface-mount, 5-A 40-V, Schottky
PCB	9-square inch, single-sided, 2-oz. copper (0.0028")

**Figure 41. Junction Temperature Rise, TO-263**

## 12 デバイスおよびドキュメントのサポート

### 12.1 コミュニティ・リソース

The following links connect to TI community resources. Linked contents are provided "AS IS" by the respective contributors. They do not constitute TI specifications and do not necessarily reflect TI's views; see TI's [Terms of Use](#).

**TI E2E™ Online Community** *TI's Engineer-to-Engineer (E2E) Community*. Created to foster collaboration among engineers. At e2e.ti.com, you can ask questions, share knowledge, explore ideas and help solve problems with fellow engineers.

**Design Support** *TI's Design Support* Quickly find helpful E2E forums along with design support tools and contact information for technical support.

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### 12.4 Glossary

**SLYZ022** — *TI Glossary*.

This glossary lists and explains terms, acronyms, and definitions.

## 13 メカニカル、パッケージ、および注文情報

以降のページには、メカニカル、パッケージ、および注文に関する情報が記載されています。これらの情報は、指定のデバイスに対して提供されている最新のデータです。このデータは予告なく変更されることがあり、ドキュメントが改訂される場合もあります。本データシートのブラウザ版を使用されている場合は、画面左側の説明をご覧ください。

**PACKAGING INFORMATION**

Orderable Device	Status (1)	Package Type	Package Drawing	Pins	Package Qty	Eco Plan (2)	Lead/Ball Finish (6)	MSL Peak Temp (3)	Op Temp (°C)	Device Marking (4/5)	Samples
LM2596S-12/NOPB	ACTIVE	DDPAK/ TO-263	KTT	5	45	Pb-Free (RoHS Exempt)	CU SN	Level-3-245C-168 HR		LM2596S -12 P+	<a href="#">Samples</a>
LM2596S-3.3	NRND	DDPAK/ TO-263	KTT	5	45	TBD	Call TI	Call TI		LM2596S -3.3 P+	
LM2596S-3.3/NOPB	ACTIVE	DDPAK/ TO-263	KTT	5	45	Pb-Free (RoHS Exempt)	CU SN	Level-3-245C-168 HR		LM2596S -3.3 P+	<a href="#">Samples</a>
LM2596S-5.0	NRND	DDPAK/ TO-263	KTT	5	45	TBD	Call TI	Call TI		LM2596S -5.0 P+	
LM2596S-5.0/NOPB	ACTIVE	DDPAK/ TO-263	KTT	5	45	Pb-Free (RoHS Exempt)	CU SN	Level-3-245C-168 HR		LM2596S -5.0 P+	<a href="#">Samples</a>
LM2596S-ADJ/NOPB	ACTIVE	DDPAK/ TO-263	KTT	5	45	Pb-Free (RoHS Exempt)	CU SN	Level-3-245C-168 HR	-40 to 125	LM2596S -ADJ P+	<a href="#">Samples</a>
LM2596SX-12/NOPB	ACTIVE	DDPAK/ TO-263	KTT	5	500	Pb-Free (RoHS Exempt)	CU SN	Level-3-245C-168 HR		LM2596S -12 P+	<a href="#">Samples</a>
LM2596SX-3.3	NRND	DDPAK/ TO-263	KTT	5	500	TBD	Call TI	Call TI		LM2596S -3.3 P+	
LM2596SX-3.3/NOPB	ACTIVE	DDPAK/ TO-263	KTT	5	500	Pb-Free (RoHS Exempt)	CU SN	Level-3-245C-168 HR		LM2596S -3.3 P+	<a href="#">Samples</a>
LM2596SX-5.0/NOPB	ACTIVE	DDPAK/ TO-263	KTT	5	500	Pb-Free (RoHS Exempt)	CU SN	Level-3-245C-168 HR		LM2596S -5.0 P+	<a href="#">Samples</a>
LM2596SX-ADJ	NRND	DDPAK/ TO-263	KTT	5	500	TBD	Call TI	Call TI	-40 to 125	LM2596S -ADJ P+	
LM2596SX-ADJ/NOPB	ACTIVE	DDPAK/ TO-263	KTT	5	500	Pb-Free (RoHS Exempt)	CU SN	Level-3-245C-168 HR	-40 to 125	LM2596S -ADJ P+	<a href="#">Samples</a>
LM2596T-12/LF03	ACTIVE	TO-220	NDH	5	45	Green (RoHS & no Sb/Br)	CU SN	Level-1-NA-UNLIM		LM2596T -12 P+	<a href="#">Samples</a>
LM2596T-12/NOPB	ACTIVE	TO-220	NDH	5	45	Green (RoHS & no Sb/Br)	CU SN	Level-1-NA-UNLIM		LM2596T -12 P+	<a href="#">Samples</a>
LM2596T-3.3/LF03	ACTIVE	TO-220	NDH	5	45	Green (RoHS & no Sb/Br)	CU SN	Level-1-NA-UNLIM		LM2596T -3.3 P+	<a href="#">Samples</a>
LM2596T-3.3/NOPB	ACTIVE	TO-220	NDH	5	45	Green (RoHS & no Sb/Br)	CU SN	Level-1-NA-UNLIM		LM2596T -3.3 P+	<a href="#">Samples</a>
LM2596T-5.0	NRND	TO-220	NDH	5	45	TBD	Call TI	Call TI		LM2596T -5.0 P+	

Orderable Device	Status (1)	Package Type	Package Drawing	Pins	Package Qty	Eco Plan (2)	Lead/Ball Finish (6)	MSL Peak Temp (3)	Op Temp (°C)	Device Marking (4/5)	Samples
LM2596T-5.0/LF03	ACTIVE	TO-220	NDH	5	45	Green (RoHS & no Sb/Br)	CU SN	Level-1-NA-UNLIM		LM2596T -5.0 P+	<a href="#">Samples</a>
LM2596T-5.0/NOPB	ACTIVE	TO-220	NDH	5	45	Green (RoHS & no Sb/Br)	CU SN	Level-1-NA-UNLIM		LM2596T -5.0 P+	<a href="#">Samples</a>
LM2596T-ADJ	NRND	TO-220	NDH	5	45	TBD	Call TI	Call TI	-40 to 125	LM2596T -ADJ P+	
LM2596T-ADJ/LF02	ACTIVE	TO-220	NEB	5	45	Green (RoHS & no Sb/Br)	CU SN	Level-1-NA-UNLIM		LM2596T -ADJ P+	<a href="#">Samples</a>
LM2596T-ADJ/NOPB	ACTIVE	TO-220	NDH	5	45	Green (RoHS & no Sb/Br)	CU SN	Level-1-NA-UNLIM	-40 to 125	LM2596T -ADJ P+	<a href="#">Samples</a>

(1) The marketing status values are defined as follows:

**ACTIVE:** Product device recommended for new designs.

**LIFEBUY:** TI has announced that the device will be discontinued, and a lifetime-buy period is in effect.

**NRND:** Not recommended for new designs. Device is in production to support existing customers, but TI does not recommend using this part in a new design.

**PREVIEW:** Device has been announced but is not in production. Samples may or may not be available.

**OBSELETE:** TI has discontinued the production of the device.

(2) **RoHS:** TI defines "RoHS" to mean semiconductor products that are compliant with the current EU RoHS requirements for all 10 RoHS substances, including the requirement that RoHS substance do not exceed 0.1% by weight in homogeneous materials. Where designed to be soldered at high temperatures, "RoHS" products are suitable for use in specified lead-free processes. TI may reference these types of products as "Pb-Free".

**RoHS Exempt:** TI defines "RoHS Exempt" to mean products that contain lead but are compliant with EU RoHS pursuant to a specific EU RoHS exemption.

**Green:** TI defines "Green" to mean the content of Chlorine (Cl) and Bromine (Br) based flame retardants meet JS709B low halogen requirements of <=1000ppm threshold. Antimony trioxide based flame retardants must also meet the <=1000ppm threshold requirement.

(3) MSL, Peak Temp. - The Moisture Sensitivity Level rating according to the JEDEC industry standard classifications, and peak solder temperature.

(4) There may be additional marking, which relates to the logo, the lot trace code information, or the environmental category on the device.

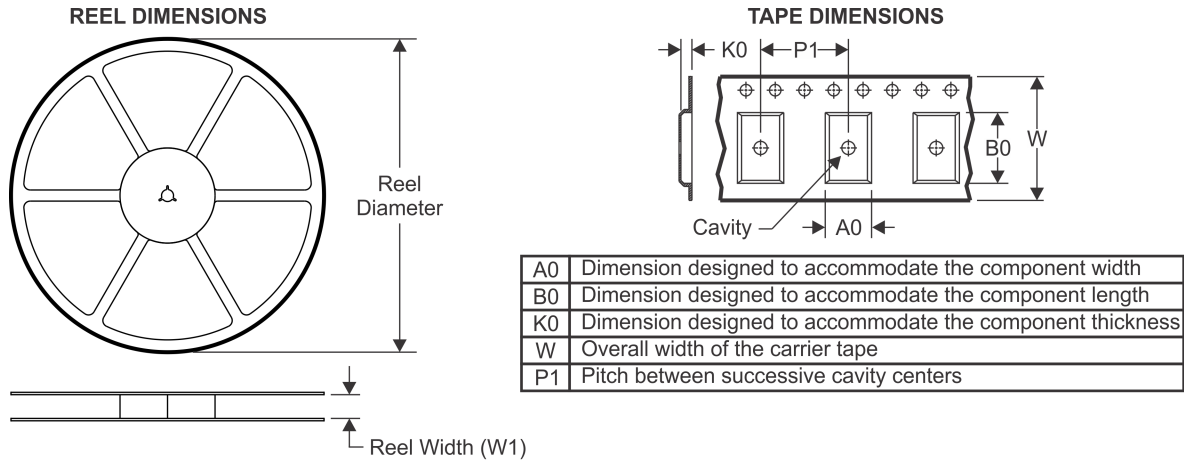
(5) Multiple Device Markings will be inside parentheses. Only one Device Marking contained in parentheses and separated by a "-" will appear on a device. If a line is indented then it is a continuation of the previous line and the two combined represent the entire Device Marking for that device.

(6) Lead/Ball Finish - Orderable Devices may have multiple material finish options. Finish options are separated by a vertical ruled line. Lead/Ball Finish values may wrap to two lines if the finish value exceeds the maximum column width.

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**TAPE AND REEL INFORMATION**

**QUADRANT ASSIGNMENTS FOR PIN 1 ORIENTATION IN TAPE**


\*All dimensions are nominal

Device	Package Type	Package Drawing	Pins	SPQ	Reel Diameter (mm)	Reel Width W1 (mm)	A0 (mm)	B0 (mm)	K0 (mm)	P1 (mm)	W (mm)	Pin1 Quadrant
LM2596SX-12/NOPB	DDPAK/ TO-263	KTT	5	500	330.0	24.4	10.75	14.85	5.0	16.0	24.0	Q2
LM2596SX-3.3	DDPAK/ TO-263	KTT	5	500	330.0	24.4	10.75	14.85	5.0	16.0	24.0	Q2
LM2596SX-3.3/NOPB	DDPAK/ TO-263	KTT	5	500	330.0	24.4	10.75	14.85	5.0	16.0	24.0	Q2
LM2596SX-5.0/NOPB	DDPAK/ TO-263	KTT	5	500	330.0	24.4	10.75	14.85	5.0	16.0	24.0	Q2
LM2596SX-ADJ	DDPAK/ TO-263	KTT	5	500	330.0	24.4	10.75	14.85	5.0	16.0	24.0	Q2
LM2596SX-ADJ/NOPB	DDPAK/ TO-263	KTT	5	500	330.0	24.4	10.75	14.85	5.0	16.0	24.0	Q2

**TAPE AND REEL BOX DIMENSIONS**

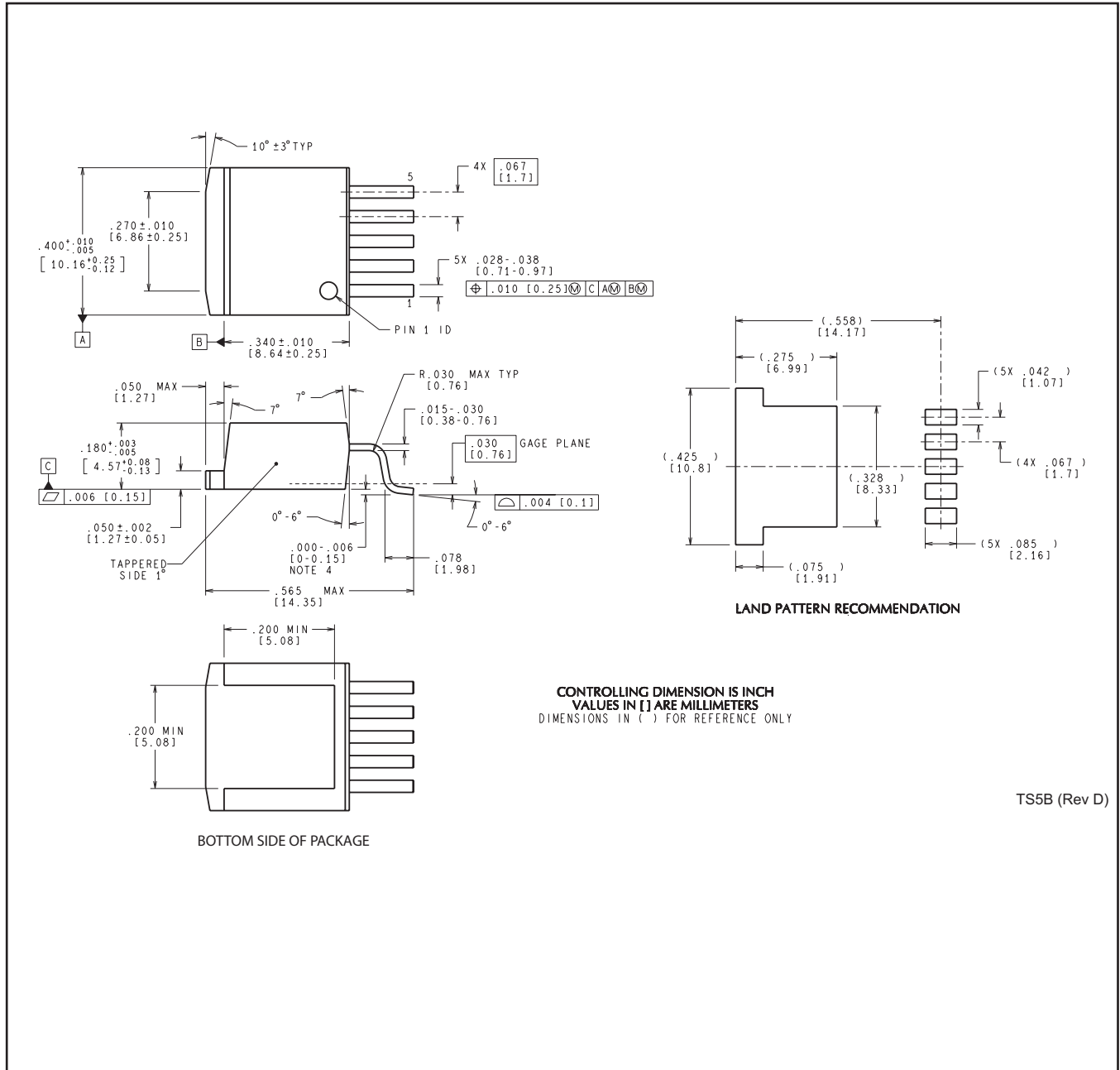

\*All dimensions are nominal

Device	Package Type	Package Drawing	Pins	SPQ	Length (mm)	Width (mm)	Height (mm)
LM2596SX-12/NOPB	DDPAK/TO-263	KTT	5	500	367.0	367.0	45.0
LM2596SX-3.3	DDPAK/TO-263	KTT	5	500	367.0	367.0	45.0
LM2596SX-3.3/NOPB	DDPAK/TO-263	KTT	5	500	367.0	367.0	45.0
LM2596SX-5.0/NOPB	DDPAK/TO-263	KTT	5	500	367.0	367.0	45.0
LM2596SX-ADJ	DDPAK/TO-263	KTT	5	500	367.0	367.0	45.0
LM2596SX-ADJ/NOPB	DDPAK/TO-263	KTT	5	500	367.0	367.0	45.0





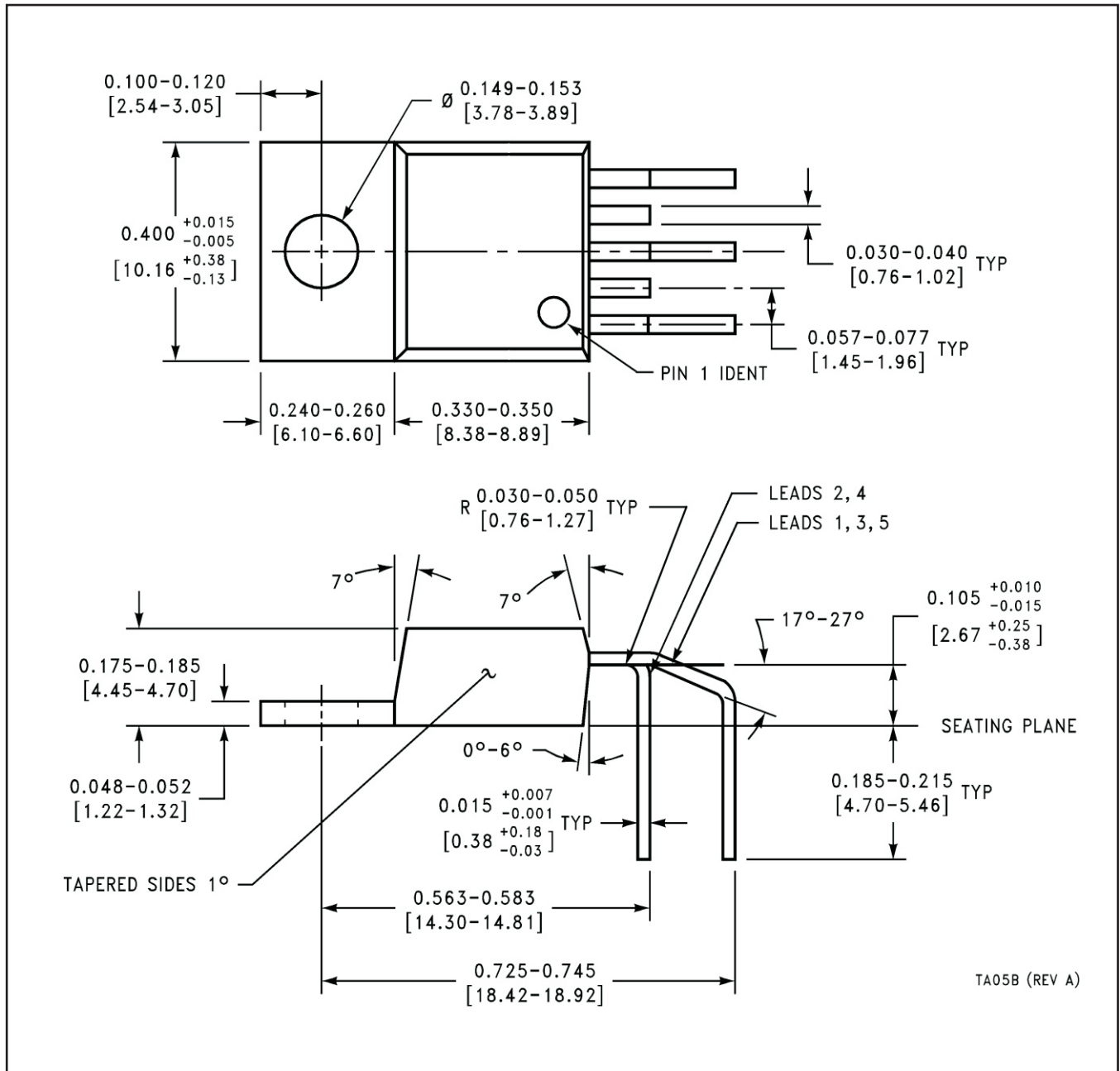
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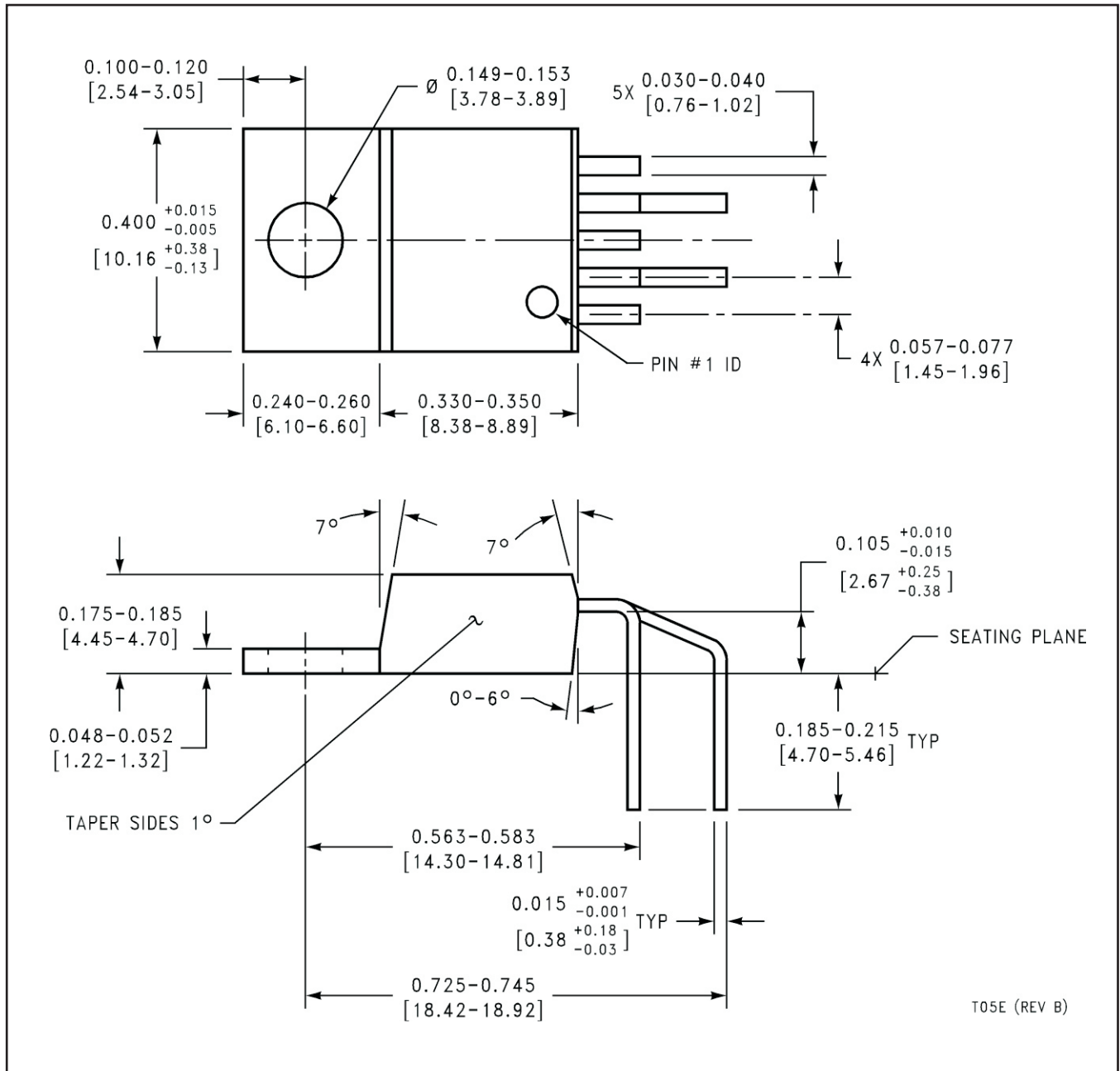
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TS5B (Rev D)

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NEB0005E



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TIデータシートに記載されているTI情報の重要な部分の複製は、その情報に一切の変更を加えることなく、かつ、その情報に関連するすべての保証、条件、制限、通知が付属する場合のみ許可されます。このような複製文書について、TIは一切の責任または義務を負いません。第三者の情報については、さらに別の制限が課される可能性があります。TI製品またはサービスの再販において、その製品またはサービスについてTIが規定したパラメータと異なるか、それを超越する記述を付すことは不公正かつ欺瞞的な商慣習であり、そのような場合、関連するTI製品またはサービスに関する明示的および黙示的な保証のすべてが無効となります。このような記述について、TIは一切責任または義務を負いません。

購入者、およびTI製品を組み込んだシステムを開発する他者(以下、「設計者」と総称します)は、自らのアプリケーションの設計において、独自の分析、評価、判断を行う責任は設計者自身にあること、および、設計者のアプリケーション(および、設計者のアプリケーションに使用されるすべてのTI製品)の安全性、および該当するすべての規制、法、その他適用される要件の遵守を保証するすべての責任は設計者のみが負うことを理解し、同意するものとします。設計者は、自身のアプリケーションに関して、(1) 危険な不具合から生じる結果を予期し、(2) 不具合およびその結果を監視し、また、(3) 害を及ぼす不具合の可能性を低減するため、保全策を策定および実施し、かつ、適切な是正措置を講じるうえで必要な専門的知識を持つことを表明するものとします。設計者は、TI製品を含むいずれかのアプリケーションを使用または配布する前に、そのアプリケーション、および、アプリケーションで使用されるTI製品の機能を完全にテストすることに同意するものとします。

TIの技術、アプリケーションまたはその他の設計に関する助言、品質特性、信頼性のデータ、もしくは、他のサービスまたは情報は、TI製品を組み込んだアプリケーションを開発する設計者に役立つことを目的として提供されるものです。これにはリファレンス設計や、評価モジュールに関係する資料が含まれますが、これらに限られません(以下、これらを総称して「TIリソース」とします)。いかなる方法であっても、TIリソースのいずれかをダウンロード、アクセス、または使用した場合、設計者(個人、または会社を代表している場合には設計者の会社)は、TIリソースをここに記載された目的のみ使用し、この注意事項の条項に従うことに同意したものとします。

TIによるTIリソースの提供は、TI製品に対する該当の発行済み保証事項または免責事項を、拡張、またはどのような形でも変更するものではなく、これらのTIリソースを提供することによって、TIにはいかなる追加義務または責任も発生しません。TIは、自社のTIリソースに訂正、拡張、改良、および、その他の変更を加える権利を留保します。TIは、特定のTIリソース用に発行されたドキュメントで明示的に記載されている以外のテストを実行していません。

設計者は、個別のTIリソースを、そのTIリソースに記載されているTI製品を搭載したアプリケーションの開発に関連する目的でのみ、使用、複製、および改変することが認められています。明示または黙示を問わず、禁反言の法理その他どのような理由でも、他のTIの知的所有権に対するその他のライセンスは与えられず、ITまたはいかなる第三者のテクノロジーまたは知的所有権についても、いかなるライセンスも与えるものではありません。これには、TI製品またはサービスが使用される組み合わせ、機械、またはプロセスに関連する特許権、著作権、回路配置利用権、その他の知的所有権が含まれますが、これらに限られません。第三者の製品やサービスに関する、またはそれらを参照する情報は、そのような製品またはサービスを利用するライセンスを構成するものではなく、それらに対する保証または推奨を意味するものでもありません。TIリソースを使用するため、第三者の特許または他の知的所有権に基づく第三者からのライセンス、もしくは、TIの特許または他の知的所有権に基づくTIからのライセンスが必要な場合があります。

TIのリソースは、それに含まれるあらゆる欠陥も含めて、「現状のまま」提供されます。TIは、TIリソースまたはその使用に関して、明示か黙示かにかかわらず、他のいかなる保証または表明も行いません。これには、正確性または完全性、権原、統発性の障害に関する保証、ならびに、商品性、特定目的への適合性、および、第三者の知的所有権の非侵害に対する黙示の保証が含まれますが、これらに限られません。TIは、設計者への弁護または補償を行う義務はなく、行わないものとします。これには、任意の製品の組み合わせに関する、または、それらに基づく侵害の請求も含まれますが、これらに限られず、また、その事実についてTIリソースまたはその他の場所に記載されているか否かを問わないものとします。いかなる場合も、TIリソースまたはその使用に関連して、またはそれらにより発生した、実際、直接的、特別、付随的、間接的、懲罰的、偶発的、または、結果的な損害について、そのような損害の可能性についてTIが知らされていたか否かにかかわらず、TIは責任を負わないものとします。

TIが特定の業界標準(例えば、ISO/TS 16949およびISO 26262を含む。)の要求に適合していることを明示的に指定した個々の本製品でない限り、TIは、業界標準の要求事項を満たしていなかったことについて、いかなる責任も負いません。

TIが製品について、機能的安全性の促進、または業界の機能的安全性基準の遵守を特に推進している場合、そのような製品は、お客様が該当の機能的安全性基準および要件を満たすアプリケーションを自ら設計および製作するために役立つことを意図したものです。アプリケーションにこれらの製品を使用することのみで、アプリケーションの安全性が確立されるものではありません。設計者は、自らのアプリケーションについて、該当する安全性関連の要件および基準の遵守を保証する必要があります。設計者は、安全でないことが致命的となる医療機器にTI製品を使用してはいけません。但し、両当事者の権限のある役員間で、かかる使用について具体的に規定した特別な契約が締結された場合はその限りではありません。安全でないことが致命的となる医療機器とは、かかる機器の不具合が重大な身体的障害又は死亡を引き起こすものを指し、生命維持装置、ペースメーカー、除細動器、心臓マッサージ機、神経刺激装置および移植医療機器を含みます。かかる機器には米国の食品医薬品局(FDA)がクラスIIIに指定するもの、また、米国外で同等に分類されているものを含みますがこれらに限られません。

TIは、特定の本製品が特別な品質(Q100、軍需対応グレード品、機能強化製品を例とする。)を満たしていることを明示的に指定することがあります。設計者は、自らのアプリケーションに適した品質が確保された本製品を選択するために必要な専門的知識を持ち、かつ、本製品の選択は買主の責任で行うことに同意するものとします。設計者は、かかる選択に関連して、法規制で要求される事項を遵守する責任を単独で負うものとします。

設計者は、自らがこのお知らせの条項および条件に従わなかったために発生した、いかなる損害、コスト、損失、責任からも、TIおよびその代表者を完全に免責するものとします。